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**Article:**

Robinson, M P orcid.org/0000-0003-1767-5541, Benson, T M, Christopoulos, C et al. (5 more authors) (1998) Analytical formulation for the shielding effectiveness of enclosures with apertures. IEEE Transactions on Electromagnetic Compatibility. pp. 240-248. ISSN: 0018-9375

<https://doi.org/10.1109/15.709422>

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# Analytical Formulation for the Shielding Effectiveness of Enclosures with Apertures

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**Abstract**—An analytical formulation has been developed for the shielding effectiveness of a rectangular enclosure with an aperture. Both the magnetic and electric shielding may be calculated as a function of frequency, enclosure dimensions, aperture dimensions and position within the enclosure. Theoretical values of shielding effectiveness are in good agreement with measurements. The theory has been extended to account for circular apertures, multiple apertures, and the effect of the enclosure contents.

**Index Terms**—Apertures, circuit modeling, electromagnetic compatibility, electrical equipment enclosures, electromagnetic shielding.

## I. INTRODUCTION

ELECTROMAGNETIC shielding is frequently used to reduce the emissions or improve the immunity of electronic equipment. The ability of a shielding enclosure to do this is characterized by its shielding effectiveness, defined as the ratio of field strengths in the presence and absence of the enclosure. At each point in an enclosure, we can define an electric shielding effectiveness  $S_E$  and a magnetic shielding effectiveness  $S_M$ .

For an infinite conducting sheet illuminated by a plane wave,  $S_E$  and  $S_M$  are equal and depend only on the frequency and on the conductivity, permeability, and thickness of the sheet. However, if an enclosure is made from the sheet, then  $S_E$  and  $S_M$  are generally different and become dependent on the position within the enclosure. Furthermore, it is practically found that the shielding is determined mainly by penetration of energy through apertures in the enclosure rather than through the walls, although an exception to this finding can be  $S_M$  at audio frequencies. In this paper, we assume that the conductivity of the enclosure walls is sufficiently high that only aperture penetration is important.

Shielding effectiveness can be calculated by numerical simulation or by analytical formulations. Numerical methods can model complex structures but often require much computing time and memory in order to model a problem with sufficient

detail. This means that although they are good at predicting the shielding of a particular enclosure, it is difficult for designers to use them to investigate the effect of design parameters on  $S_E$  and  $S_M$ . Numerical methods that have been used to calculate shielding include transmission-line modeling [1], finite-difference time-domain (FDTD) method [2], and method of moments (MoM) [3].

Analytical formulations provide a much faster means of calculating shielding effectiveness, enabling the effect of design parameters to be investigated (we use the term formulation rather than solution, as they often use empirical relationships rather than fundamental principles). Many of these are derived from Bethe's theory of diffraction through holes [4] and apply only to electrically small apertures. Other formulations include that of Hill *et al.* [5], derived from a power-balance method and the widely quoted formula of Ott  $S_E = 20 \log_{10} \lambda/2l$  [6], where  $\lambda$  is wavelength and  $l$  is aperture length.

Our aim here has been to derive a relatively simple formulation that incorporates all the relevant design parameters without placing inconvenient restrictions on their range. We follow Mendez [7] in considering the enclosure as a waveguide, and assume a single mode of propagation (the  $TE_{10}$  mode). However, our formulation applies above the cutoff frequency for this mode as well as below. Both electric and magnetic shielding are calculated as functions of frequency, aperture dimensions, enclosure dimensions, wall thickness, and position within the enclosure. Simple modifications enable multiple apertures and internal losses to be included. At present, our formulation applies only to rectangular enclosures, but these comprise a large proportion of shields used in practical electronic design. It may be applied to electrically large and small apertures.

## II. THEORY

A rectangular aperture in an empty rectangular enclosure is represented by the equivalent circuit of Robinson *et al.* [8], which is shown in Fig. 1. The longer side of the slot is shown normal to the  $E$ -field, which is the worst case for shielding. The electric shielding at a distance  $p$  from the slot is obtained from the voltage at point  $P$  in the equivalent circuit, while the current at  $P$  gives the magnetic shielding. The radiating source is represented by voltage  $V_0$  and impedance  $Z_0 \simeq 377 \Omega$  and the enclosure by the shorted waveguide whose characteristic impedance and propagation constant are  $Z_g$  and  $k_g$ . We

Manuscript received March 26, 1997; revised May 27, 1998. This work was supported by the Engineering and Physical Sciences Research Council under Grants GR/J09086 and GR/J10396.

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Publisher Item Identifier S 0018-9375(98)06191-2.

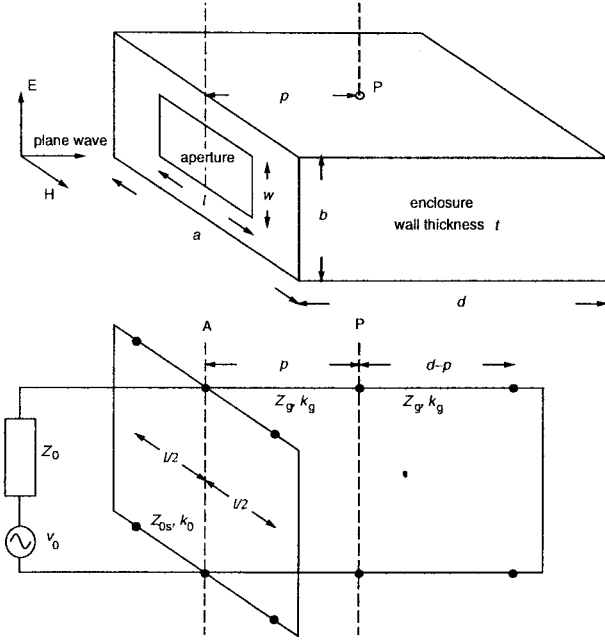


Fig. 1. Rectangular box with aperture and its equivalent circuit.

proceed by first finding an equivalent impedance for the slot and then using simple transmission line theory to transform all the voltages and impedances to point  $P$ .

#### A. Slot Impedance

The aperture is represented as a length of coplanar strip transmission line, shorted at each end (implying that we need only consider the transmission line currents on the front face of the enclosure). The total width is equal to the height of the enclosure  $b$  and the separation is equal to the width of the slot  $w$ . Its characteristic impedance is given by Gupta *et al.* [9] as  $Z_{0s} = 120\pi K(w_e/b)/K'(w_e/b)$ , where  $K$  and  $K'$  are elliptic integrals. The effective width  $w_e$  is given by

$$w_e = w - \frac{5t}{4\pi} \left( 1 + \ln \frac{4\pi w}{t} \right) \quad (1)$$

where  $t$  is the thickness of the enclosure wall. If  $w_e < b/\sqrt{2}$  (which is true for most practical apertures) then, according to Gupta *et al.*, the following approximation may be used:

$$Z_{0s} = 120\pi^2 \left[ \ln \left( 2 \frac{1 + \sqrt[4]{1 - (w_e/b)^2}}{1 - \sqrt[4]{1 - (w_e/b)^2}} \right) \right]^{-1}. \quad (2)$$

Fig. 2 shows this variation of  $Z_{0s}$  with  $w_e/b$ .

To calculate the aperture impedance  $Z_{ap}$ , we transform the short circuits at the ends of the aperture through a distance  $l/2$  to the center. This is represented by point  $A$  in the equivalent circuit. It is necessary here to include a factor  $l/a$  to account for the coupling between the aperture and the enclosure

$$Z_{ap} = \frac{1}{2} \frac{l}{a} j Z_{0s} \tan \frac{k_0 l}{2}. \quad (3)$$

This accounts for the connection between transmission line and waveguide.

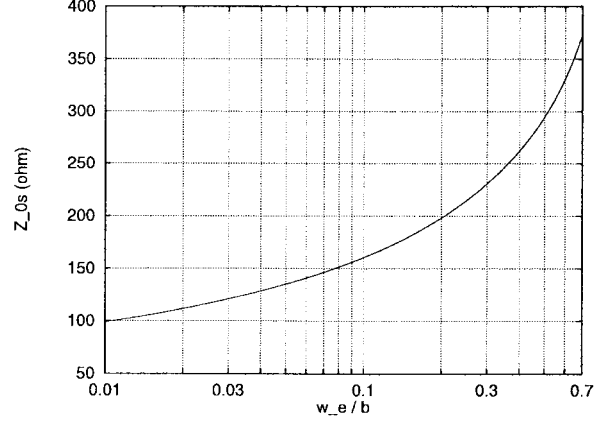


Fig. 2. Characteristic impedance  $Z_{0s}$  of aperture as a function of  $w_e/b$ .

#### B. Electric and Magnetic Shielding Effectiveness

By Thèvenin's theorem, combining  $Z_0$ ,  $v_0$ , and  $Z_{ap}$  gives an equivalent voltage  $v_1 = v_0 Z_{ap}/(Z_0 + Z_{ap})$  and source impedance  $Z_1 = Z_0 Z_{ap}/(Z_0 + Z_{ap})$ . For the  $TE_{10}$  mode of propagation, the waveguide has characteristic impedance  $Z_g = Z_0/\sqrt{1 - (\lambda/2a)^2}$  and propagation constant  $k_g = k_0\sqrt{1 - (\lambda/2a)^2}$ , where  $k_0 = 2\pi/\lambda$ . Note that  $Z_g$  and  $k_g$  are imaginary at frequencies below the cutoff (equal to  $c_0/2a$ ). We now transform  $v_1$ ,  $Z_1$ , and the short circuit at the end of the waveguide to  $P$ , giving an equivalent voltage  $v_2$ , source impedance  $Z_2$ , and load impedance  $Z_3$

$$v_2 = \frac{v_1}{\cos k_g p + j(Z_1/Z_g) \sin k_g p} \quad (4)$$

$$Z_2 = \frac{Z_1 + j Z_g \tan k_g p}{1 + j(Z_1/Z_g) \tan k_g p} \quad (5)$$

$$Z_3 = j Z_g \tan k_g (d - p). \quad (6)$$

The voltage at  $P$  is now  $v_p = v_2 Z_3/(Z_2 + Z_3)$ , and the current at  $P$  is  $i_p = v_2/(Z_2 + Z_3)$ .

In the absence of the enclosure, the load impedance at  $P$  is simply  $Z_0$ . The voltage at  $P$  is  $v'_p = v_0/2$  and the current is  $i'_p = v_0/2Z_0$ . The electric and magnetic shielding are, therefore, given by

$$S_E = -20 \log_{10} |v_p/v'_p| = -20 \log_{10} |2v_p/v_0| \quad (7)$$

$$S_M = -20 \log_{10} |i_p/i'_p| = -20 \log_{10} |2i_p Z_0/v_0|. \quad (8)$$

#### C. Extensions to the Formula

We have extended the theory to account for electromagnetic losses, circular apertures, and multiple apertures.

Circuit boards, power supplies, and other contents introduce electromagnetic losses into enclosures. This affects their shielding effectiveness, particularly at resonant frequencies [10]. As a first approximation we have assumed that these losses are uniformly distributed throughout the enclosure. Distributed losses in coaxial lines may be modeled by including a correction factor  $\zeta$  in the expressions for characteristic impedance and propagation constant [11]. Adopting a similar approach for the shielding formulation gives a modified

TABLE I  
ENCLOSURES USED FOR SHIELDING MEASUREMENTS

$a(\text{mm})$	$b(\text{mm})$	$d(\text{mm})$	$t(\text{mm})$	material
300	120	300	1.5	brass
483	120	483	1.5	brass
146	55	222	2.5	Al/Mg alloy
222	55	146	2.5	Al/Mg alloy

characteristic impedance  $Z'_g$  and propagation constant  $k'_g$

$$Z'_g = (1 + \zeta - j\zeta)Z_g \quad (9)$$

$$k'_g = (1 + \zeta - j\zeta)k_g. \quad (10)$$

These can be substituted for  $Z_g$  and  $k_g$  in the calculations in Section II-B.

Turner *et al.* [12] have found that the shielding effectiveness of a round hole is approximately the same as that of that of a square aperture of the same area. The formulation can, therefore, be applied to circular apertures by letting

$$l = w = \frac{\sqrt{\pi}}{2}d_h \quad (11)$$

where  $d_h$  is the diameter of the aperture.

If there are  $n$  similar apertures in one face of the enclosure, then the individual aperture impedances must be combined. We have assumed that the individual impedances may simply be combined in series, giving a total impedance

$$Z_{ap} = n \frac{1}{2} \frac{l}{a} jZ_{0s} \tan \frac{k_0 l}{2}. \quad (12)$$

The calculations then proceed as in Section II-B. This simple approach ignores the mutual admittance between apertures and may not be applicable if the apertures are too close together.

### III. MEASUREMENTS

The shielding effectiveness of a range of enclosures and apertures was measured. Apertures were either cut into the walls of the enclosures or into removable plates. These were attached with finger stock to ensure good contact at the joints. The lids of the enclosures were fastened with gaskets, finger stock, or closely spaced screws for the same reason. Table I lists the relevant parameters of the enclosures. The aperture length  $l$  ranged from 40 to 200 mm and the width  $w$  from 4 to 80 mm.

Shielding measurements were made by placing sensors in the enclosure, or by observing the emissions from a radiating circuit within the enclosure. Measurements with sensors were made in screened rooms. The source of the field was a network analyzer connected via an amplifier to a stripline [13], log periodic, or Bilog [14] antenna. The rooms were dampened with absorbing material to reduce the effects of resonances. To measure  $S_E$ , a monopole antenna in the lid of the enclosure sensed the field. It was coupled via a cable or an optical link to the second port of the network analyzer. Fig. 3 shows the

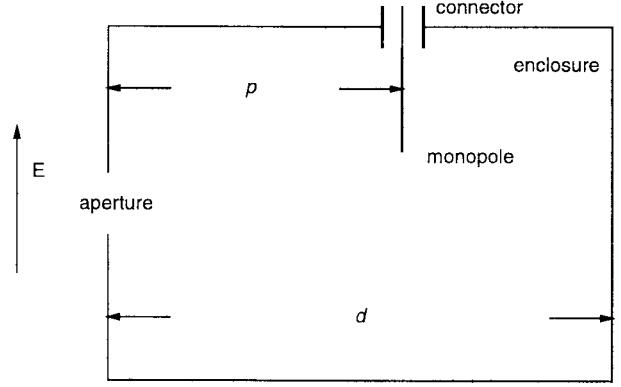


Fig. 3. Method of measuring electric shielding  $S_E$ .

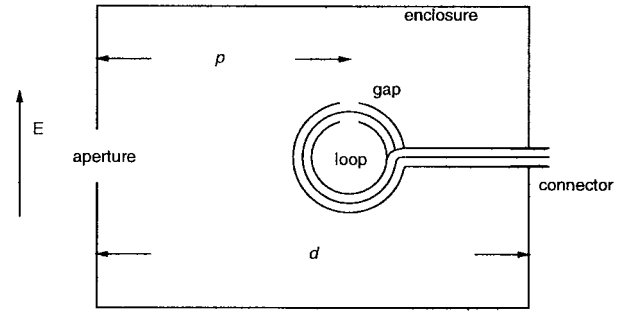


Fig. 4. Method of measuring magnetic shielding  $S_M$ .

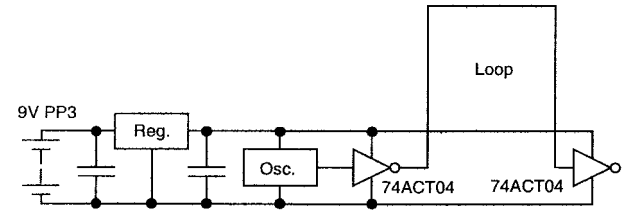


Fig. 5. Digital circuit used for measurement of shielding. Oscillator frequency 10 MHz.

orientation of the monopole in the enclosure. For calibration, a measurement of  $S_{21}$  was made using the probe and lid only.

Measurement of  $S_M$  was similar to the above except that a shielded loop was used to sense the field (only one sensor being used at a time). Fig. 4 shows how the gap in the loop was aligned with the unshielded section of the inner conductor orthogonal to the electric field, minimizing unwanted coupling. For calibration, a measurement was made using the probe only.

Shielding effectiveness was also measured by comparing the emissions from a small circuit board (size  $80 \times 60$  mm) in the presence and absence of the enclosure. Emissions were measured with a stripline from 10 to 300 MHz and a Bilog antenna from 300 to 1000 MHz. A synchronous digital circuit was used, as shown in Fig. 5. This enabled the shielding to be measured at the harmonics of the clock frequency, which was 10 MHz.

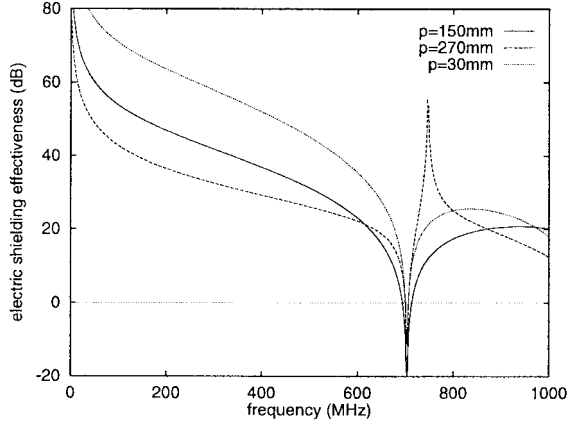


Fig. 6. Calculated  $S_E$  at three positions in  $300 \times 120 \times 300$  mm enclosure with  $100 \times 5$  mm aperture.

The monopole sensor was also used to measure  $S_E$  of the  $300 \times 120 \times 300$  mm enclosure containing lossy elements. To introduce electromagnetic losses, various unpowered circuit boards were placed in the enclosure. Blocks of radio absorbing material (RAM) were also used. These were placed on the floor of the enclosure, and offset from the center to prevent them touching the sensor. The blocks were 130 mm wide (i.e., parallel to the slot), 60 mm high (i.e., perpendicular to the slot), and 5–50 mm thick (i.e., along the direction of propagation). The effect of block thickness on the shielding was investigated.

#### IV. RESULTS

##### A. Electric Shielding Effectiveness

Fig. 6 shows the calculated  $S_E$  at three positions within the unloaded  $300 \times 300 \times 120$  mm enclosure with a  $100 \times 5$  mm aperture. The calculations show that the enclosure resonates at approximately 700 MHz, leading to negative shielding (field enhancement) around this frequency. Below the resonant frequency,  $S_E$  decreases with frequency and increases with distance from the aperture.

Fig. 7 shows the calculated and measured  $S_E$  at the center of the box ( $p = 150$  mm). We can see that there is good agreement, both above and below the cutoff frequency of 500 MHz. Note that much of the variation in the measurements is due to the imperfect damping of resonances in the screened room. These shift in frequency when the enclosure is placed in the room, leading to the “noisy” appearance of the plots of shielding versus frequency. The agreement at the two other positions ( $p = 30$  mm and  $p = 270$  mm) was also good. Fig. 8 shows the calculated and measured  $S_E$  for a larger aperture, size  $200 \times 30$  mm. The resonance is broader and the low-frequency shielding is worse than that of the smaller aperture.

Fig. 9 shows the calculated and measured  $S_E$  at the center of the  $222 \times 55 \times 146$  mm box while Fig. 10 shows these quantities at the center of the  $483 \times 120 \times 483$  mm box. In each case the aperture was  $100 \times 5$  mm. It can be seen from these figures that the smaller box does not resonate below 1 GHz, while the larger box shows resonances at 440 and 980 MHz.

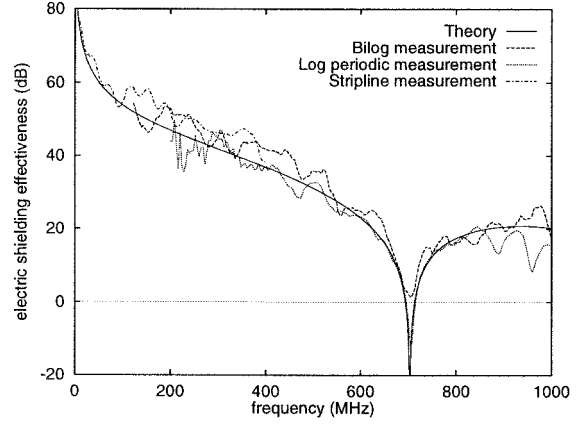


Fig. 7. Calculated and measured  $S_E$  at center of  $300 \times 120 \times 300$  mm enclosure with  $100 \times 5$  mm aperture.

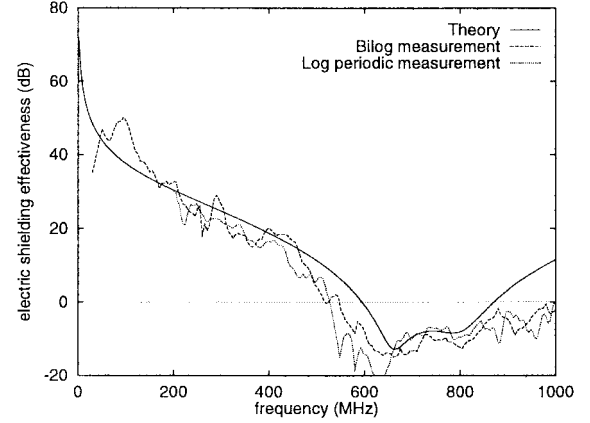


Fig. 8. Calculated and measured  $S_E$  at center of  $300 \times 120 \times 300$  mm enclosure with  $200 \times 30$  mm aperture.

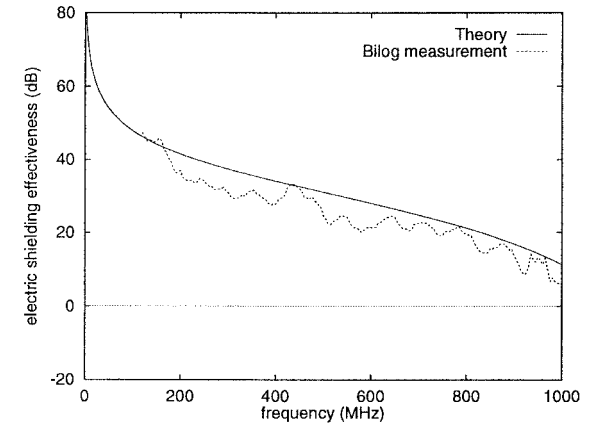


Fig. 9. Calculated and measured  $S_E$  at center of  $222 \times 55 \times 146$  mm enclosure with  $100 \times 5$  mm aperture.

##### B. Magnetic Shielding Effectiveness

Fig. 11 shows  $S_M$  of the  $300 \times 300 \times 120$  mm enclosure with a  $100 \times 5$  mm aperture, calculated at  $p = 30, 150$ , and 270 mm (the same positions as in Fig. 6). The enclosure

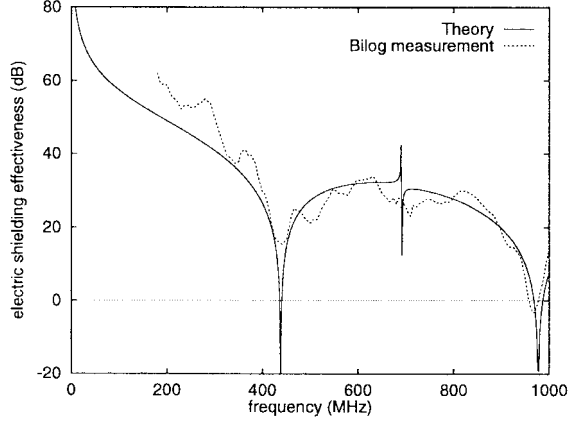


Fig. 10. Calculated and measured  $S_E$  at center of  $483 \times 120 \times 483$  mm enclosure with  $100 \times 5$  mm aperture.

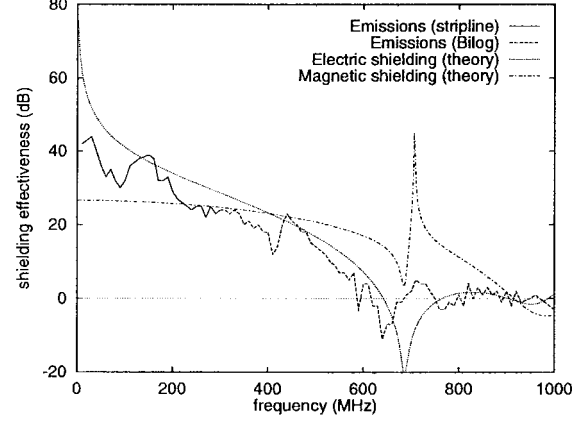


Fig. 12. Emissions measurement of shielding at center of  $300 \times 120 \times 300$  mm enclosure with  $150 \times 40$  mm aperture compared to calculated  $S_E$  and  $S_M$ .

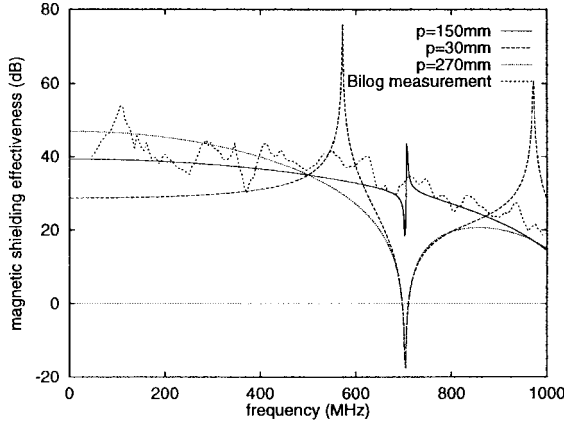


Fig. 11. Calculated  $S_M$  at three positions in  $300 \times 120 \times 300$  mm enclosure with  $100 \times 5$  mm aperture, and measured  $S_M$  at center of enclosure.

resonance at 700 MHz can be seen at  $p = 30$  mm and  $p = 270$  mm, but is less pronounced at the center of the box ( $p = 150$  mm). This is expected from the mode structure of the resonance. At low frequencies,  $S_M$  increases with distance from the aperture (as does  $S_E$ ), but is almost independent of frequency.

Fig. 11 also shows that there is good agreement between calculated and measured  $S_M$  at the center of the box ( $p = 150$  mm). Agreement was also good at  $p = 240$  mm, where the resonance at 700 MHz was seen in the measurements. Agreement was slightly worse just behind the slot ( $p = 30$  mm), with the calculated values of  $S_M$  being 5–10 dB higher than the measurements at low frequencies.

### C. Change in Emissions

Fig. 12 shows the shielding of the  $300 \times 120 \times 300$  mm enclosure with a  $150 \times 40$  mm aperture obtained from the difference in emissions between the shielded and unshielded circuit. The enclosure resonance can be seen, although its frequency is some 50 MHz lower, presumably because of the loading effect of the circuit on the enclosure. The cal-

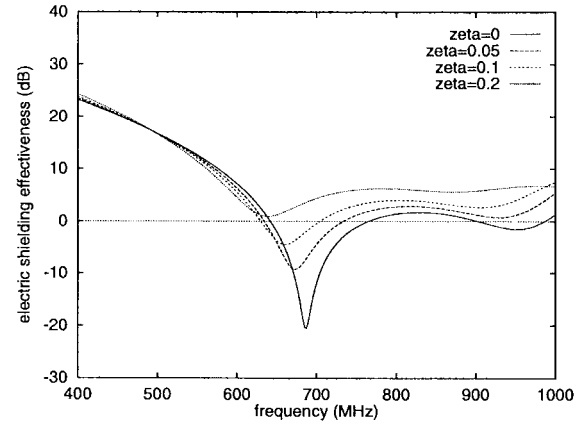


Fig. 13. Effect of loss term  $\zeta$  on calculated  $S_E$ .

culated values of  $S_E$  and  $S_M$  are also shown in Fig. 12. At low frequencies, the reduction in emissions lies between the calculated  $S_E$  and  $S_M$ . This might be expected as a typical circuit board is a source of both electric and magnetic fields.

### D. Effect of Electromagnetic Losses

Introducing the loss term  $\zeta$  into the formulation does not greatly affect the calculated shielding effectiveness, except around the resonant frequencies. Fig. 13 shows  $S_E$  at the center of the  $300 \times 300 \times 120$  mm enclosure with a  $100 \times 5$  mm aperture for various values of  $\zeta$ . We can see that increasing the loss damps the resonance, improving the shielding. It also lowers the resonant frequency.

Fig. 14 shows  $S_E$  of this enclosure and aperture with various sized blocks of RAM inside. We see that as the thickness increases, the resonant frequency shifts in the manner predicted by the theory and shown in Fig. 13. Placing single-sided circuit boards in the enclosure had a similar effect on the shielding. Fig. 15 shows this for two boards, one (PCB 1) loaded mainly with integrated circuits, resistors and capacitors, the other (PCB 2) a power supply board carrying a mains

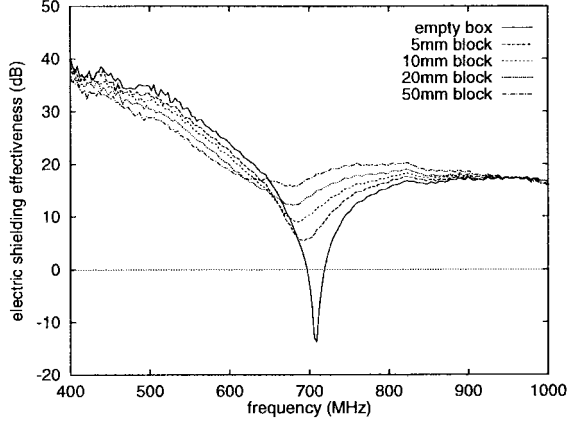


Fig. 14. Measured  $S_E$  with various sized blocks of RAM in enclosure.

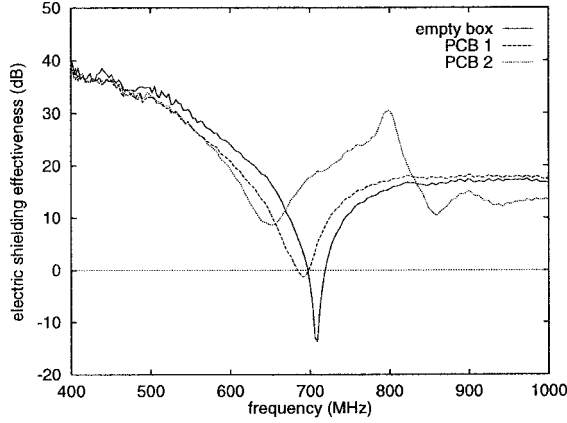


Fig. 15. Measured  $S_E$  with two different circuit boards in enclosure.

transformer. Note how PCB 2 introduces a second resonance at approximately 860 MHz.

### E. Circular Apertures

We measured  $S_E$  at the center of the  $300 \times 300 \times 120$  mm enclosure with a square aperture of side 77 mm and a circular aperture diameter 88 mm. Each aperture's area was approximately  $6000 \text{ mm}^2$ . The values of  $S_E$  for these apertures did not differ by more than 2 dB over the frequency range of 200–1000 MHz.

Fig. 16 shows the measured and calculated  $S_E$  at the center of the enclosure with the circular aperture. Also shown are the values calculated from Ott [6] and from Hill *et al.* [5]. Although these show the right frequency dependence at low frequencies, they do not predict the resonance at 700 MHz. The new formulation gives better agreement both at low frequencies and at the resonance.

We also compared our formulation with measurements described in the literature. Steenbakkers *et al.* [15] measured the magnetic shielding effectiveness at various positions in a  $150 \times 150 \times 150$  mm enclosure with a round aperture in one wall. Our analytical formulation gives values of  $S_M$

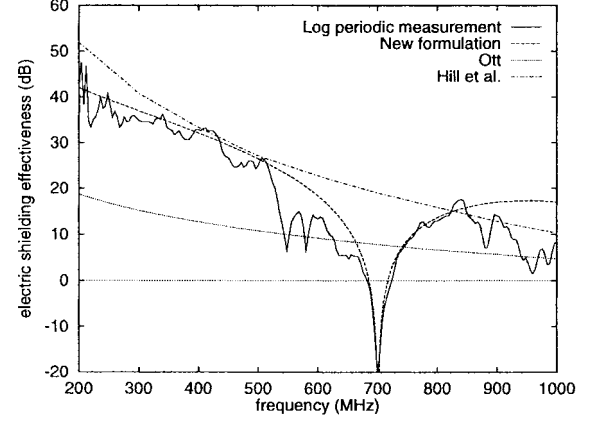


Fig. 16. Measured and calculated  $S_E$  at center of  $300 \times 120 \times 300$  mm enclosure with 88 mm diameter circular aperture.

TABLE II  
REDUCTION IN  $S_E$  DUE TO NUMBER OF APERTURES

$n$	$S_E$ (dB)	
	theory	measured
1	0	0
2	5.6	3.7 to 4.4
3	8.8	6.6 to 7.7

within 10 dB of their results. Steenbakkers *et al.* found that increasing the hole diameter from 30 to 60 mm reduced  $S_M$  by 12 dB. The analytical formulation predicts a reduction of 14 dB. The measurements of Steenbakkers *et al.* also show that at subresonant frequencies,  $S_M$  increases with distance from the aperture—an effect predicted by our formulation and seen in Fig. 11.

### F. Multiple Apertures

We measured  $S_E$  at the center of the  $300 \times 300 \times 120$  mm enclosure with one, two and three  $160 \times 4$  mm apertures. For these measurements, the box with a single aperture was used as the calibration standard. This greatly reduced the artifacts due to the resonances of the room, because merely changing the number of apertures did not significantly alter the frequencies of these resonances. Increasing the number of apertures  $n$  was found to reduce the shielding effectiveness. Table II shows the calculated reduction in  $S_E$  at 400 MHz compared to measurements over the range 200–600 MHz.

The analytical solution predicts that  $S_E$  and  $S_M$  are increased by increasing the number of apertures while keeping the total area the same. Fig. 17 shows the measured  $S_E$  at the center of the  $300 \times 300 \times 120$  mm enclosure with one, two, four, and nine apertures. In each case the total area was  $6000 \text{ mm}^2$ . As predicted, having more but smaller holes improves the shielding.

We investigated the effect of dividing a  $100 \times 5$  mm slot into several shorter slots using the same enclosure as above. Table III shows the calculated and measured increase in  $S_E$  and  $S_M$ . The measured increase is slightly more than predicted.

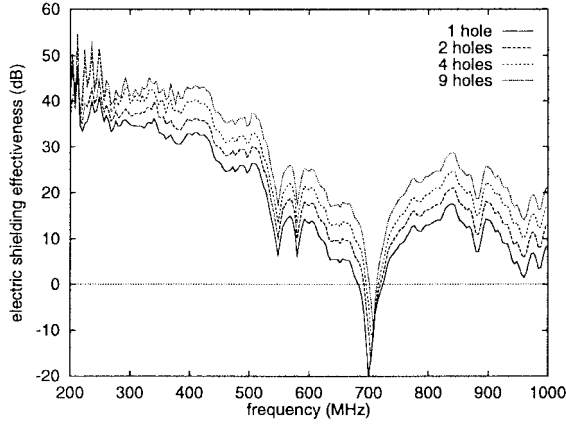


Fig. 17. Measured  $S_E$  for various numbers of circular apertures of same total area (centre of 300x120x300 mm enclosure).

TABLE III  
INCREASE IN  $S_E$  AND  $S_M$  DUE TO DIVIDING SLOT

Number of divisions	$S_E$ (dB)		$S_M$ (dB)	
	theory	measured	theory	measured
1	0	0	0	0
2	6	8 to 10	6	8 to 10
4	12	15 to 20	12	13 to 18

Fig. 18 shows  $S_E$  at the center of the same enclosure with two designs of ventilation plate, one with three  $160 \times 4$  mm slots, the other with 20 12-mm-diameter holes. Although the total area of metal removed is about the same,  $S_E$  is up to 30 dB greater for the circular holes than for the slots. The “jagged” appearance of the measured results is due to resonances in the screened room. The agreement between theory and measurements is surprisingly good, considering the simple treatment of multiple apertures in (12).

## V. DISCUSSION

The analytical formulation presented here provides a fast means of investigating the effect of design parameters on the shielding effectiveness of an enclosure. It confirms that long thin apertures are worse than round or square apertures of the same area. For a typical sized enclosure, the theory predicts that doubling the length of a slot reduces  $S_E$  and  $S_M$  by about 12 dB, while doubling the width only reduces  $S_E$  and  $S_M$  by about 2 dB. Calculations using the new formulation show that doubling the number of apertures reduces both  $S_E$  and  $S_M$  by about 6 dB. However, dividing a long slot into two shorter ones increases  $S_E$  and  $S_M$  by about 6 dB.

The theory predicts that the size of the enclosure is also important to shielding performance. At subresonant frequencies, doubling the enclosure dimensions while keeping the aperture constant is predicted to increase  $S_E$  by about 6 dB and  $S_M$  by about 13 dB. However, doubling the dimensions of both enclosure and aperture is predicted to reduce  $S_E$  by about 6 dB and  $S_M$  by about 1 dB. Furthermore, doubling the enclosure

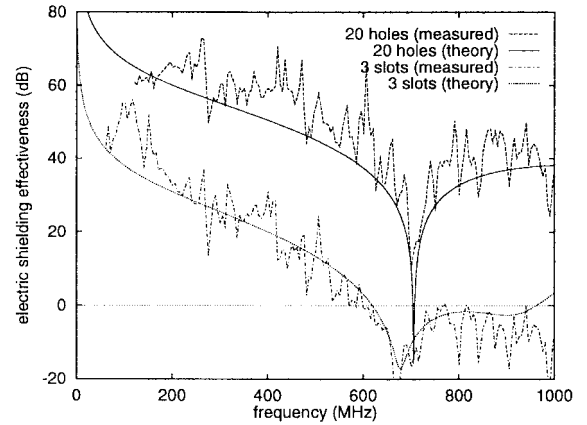


Fig. 18. Calculated and measured  $S_E$  for ventilation plates with either three 160mm long slots or twenty 12mm diameter holes (centre of 300x120x300mm enclosure).

size halves the lowest resonant frequency. A small enclosure is, therefore, generally preferable to a large one.

There are two points to make concerning the contents of the enclosure. First,  $S_E$  and  $S_M$  are lower nearer the aperture, so noisy or sensitive circuits should be placed as far from the aperture as possible. Secondly, the contents damp the enclosure resonances, mitigating the negative shielding seen at the resonant frequencies of an unloaded (i.e., empty) enclosure.

Our calculation has assumed that the conductivity of the walls of the enclosure is so high that the only significant path of energy is through the aperture. This may not always be so, particularly for low frequency magnetic fields. Field [16], following Kaden [17], gives equations for the electric and magnetic shielding of conducting spherical shells. These indicate that  $S_E$  of an unbroken shell is always high unless the walls are very thin or are poor conductors. However  $S_M$  is zero for static magnetic fields if the shell is made from nonmagnetic material. The magnetic shielding rises with frequency, first because of field cancellation by eddy currents, and then also because of the skin effect. For the enclosures and apertures investigated in this study, the frequency at which the “finite conductivity”  $S_M$  becomes comparable to the “aperture”  $S_M$  is at 10–100 kHz. Our assumption of aperture dominance is therefore valid over our measurement frequency range of 1–1000 MHz. The results of Steenbakkers *et al.* [15] suggest that there is a smooth transition between the two effects. If the enclosure was made from a coated plastic or a conductive polymer the transition would be at a higher frequency.

The analytical formulation assumes a single,  $TE_{10}$  mode of propagation. Higher order  $TE_{n0}$  modes would be able to propagate at frequencies greater than  $nc_0/2a$ . For all but the largest enclosure studied, the  $TE_{20}$  and higher modes could not propagate below 1000 MHz. For the  $483 \times 120 \times 483$  mm enclosure, the cutoff frequencies of the  $TE_{20}$  and  $TE_{30}$  modes are 621 and 931 MHz, respectively. However, Fig. 10 shows that the theory gives good agreement with measurement up to 1000 MHz. This may be because the coupling to the higher order modes is not significant for the enclosures and apertures studied. Multimode propagation in a shielded enclosure has been successfully modeled [18], but considerable work would



be needed to incorporate such calculations into the formulation discussed here.

In this study, we have placed the aperture centrally in one face of the enclosure, and considered the electromagnetic fields along the midline. For an off-center aperture (e.g., a gap underneath a lid), there might be transverse as well as longitudinal propagation. Further work is needed in this area.

An advantage of the formulation is that it accounts for the thickness of the enclosure walls. This is often difficult in numerical methods, which assume infinitesimally thin walls. The formulation might however be inaccurate if the width of the aperture  $w$  were small compared to the wall thickness  $t$ . The aperture would itself then act as a waveguide operating below its cutoff frequency, leading to attenuation within the aperture and giving greater shielding than predicted.

## VI. CONCLUSION

The formulation described above gives good agreement with measurements over a wide frequency range. It can predict the electric and magnetic shielding effectiveness of a rectangular enclosure with one or more apertures in one wall, both at low frequencies and at resonance. It can be applied to round, square, and rectangular apertures and the size of the aperture need not be small compared to the enclosure. A loss factor has been introduced to describe the damping of resonances by the contents of the enclosure, although further work is needed to characterize this factor for typical electronic equipment. The calculation of electric and magnetic shielding depends upon the frequency and polarization of the applied field, the dimensions of the enclosure and the aperture(s), the number of apertures, and the position within the enclosure. The formulation will, therefore, be of use to designers of shielded enclosures.

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Robinson, M.P.; Benson, T.M.; Christopoulos, C.; Dawson, J.F.; Ganley, M.D.; Marvin, A.C.; Porter, S.J.; Thomas, D.W.P., "Analytical formulation for the shielding effectiveness of enclosures with apertures," *Electromagnetic Compatibility, IEEE Transactions on*, vol.40, no.3, pp.240,248, Aug 1998

doi: 10.1109/15.709422

URL: <http://ieeexplore.ieee.org/stamp/stamp.jsp?tp=&arnumber=709422&isnumber=15395>