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# Cascaded Modular Multilevel Converter and Cycloconverter Based Machine Drive System

Yue Zhang, Fujin Deng, *Senior Member, IEEE*, Jiehua Hou, Pengyuan Jiang, Hanlu Zhang, Kangshun Zhu, Yihua Hu, *Senior Member, IEEE* and Sergio Vazquez, *Fellow, IEEE*

**Abstract**— Low-speed drive is one of the challenges for modular multilevel converters (MMCs) due to large capacitor voltage fluctuation. In this paper, a cascaded MMC and cycloconverter (CCV) based machine drive system is proposed to ensure stable operation of medium-voltage and low-speed machine. The MMC provides medium-frequency ac voltage for the CCV, and the CCV converts the medium-frequency ac input to low-frequency ac output required by the machine. Detailed analysis about MMC's operation frequency, device current stress and submodule (SM) capacitance are given in this paper. Proposed drive system can operate at zero/low frequency under rated load torque, while the SM capacitance is much smaller than that in existing methods. Simulation and experimental studies are conducted, and the results verify the effectiveness of proposed system.

**Index Terms**— Capacitor voltage, cycloconverter, low-speed machine drive, modular multilevel converter (MMC).

## I. INTRODUCTION

The modular multilevel converter (MMC), which was firstly proposed in 2003 [1], has become the most potential topology for next-generation medium/high-voltage applications due to its advantages such as modularity, high efficiency, and flexible expandability [2]-[7]. In recent years, the MMC is attractive for the medium-voltage drive applications.

The submodule (SM) capacitor voltage fluctuation is one of the important issues for the MMC working at low frequency. The voltage fluctuation is inversely proportional to the operation frequency of the MMC [8]. For the MMC's zero/low-speed high-torque scenarios such as hoister, conveyor and mill applications, the voltage fluctuation will be large and unacceptable, which would cause overmodulation and degrades the system reliability [9].

To date, the mainstream solution to suppress the capacitor voltage fluctuation in the MMC at low speed is the current

injection based methods [10]-[14]. Kolb *et al.* [10] presents the injection of high-frequency sinusoidal common-mode voltage and circulating current, which can eliminate the low-frequency capacitor voltage fluctuation, but the device current stress is increased [11]. To reduce the device current stress, the improved injection methods [12]-[14] are proposed for the MMC. However, the injection of high-amplitude current is still needed. The current injection based methods require to inject high-amplitude circulating current and the device current stress is extremely high especially in low-speed high-torque scenarios.

Alternatively, the capacitor voltage fluctuation in the MMC at low speed can be reduced by variable dc voltage methods [15]-[21]. Li *et al.* [15] proposes a hybrid MMC (HMMC) with a chopper on the dc side, which can change the average dc voltage along with the variation of output frequency. However, the average dc voltage cannot be reduced to zero, so the voltage fluctuation is still high at zero/low speed. Sau *et al.* [16] applies parallel SMs in [17], then the MMC operates with one SM in each arm at zero/low speed. However, the output voltage of parallel SMs is limited, which cannot satisfy the operation for medium-voltage low-speed machines. Kumar *et al.* [18] and [19] use a back-to-back (BTB) MMC, where the grid-side MMC is controlled as a current source, and the capacitor voltage fluctuation keeps unchanged. However, both the grid-side and machine-side MMCs require full-bridge SMs, which greatly increases the number of devices. Although Guan *et al.* [20] and Li *et al.* [21] reduce the devices of BTB-MMCs, the stable operation under rated torque at zero speed cannot be ensured. The variable dc voltage methods have limitation to suppress the capacitor voltage fluctuation of MMCs for medium-voltage low-speed drive, which require large SM capacitance [15], [18].

This paper proposes a cascaded MMC and cycloconverter (CCV) based machine drive system for the medium-voltage low-speed machine, which extends the work in [22]. Detailed analysis is conducted in this paper, including the operation frequency of MMCs, device current stress, and SM capacitance. In addition, a prototype of the proposed machine drive system is built in the lab and the experimental studies are conducted in this paper. In the proposed system, the MMC operates at medium frequency, providing constant ac voltage for the CCV, and the CCV converts the medium-frequency ac input to low-frequency ac output required by the machine. The paper includes following contributions: 1) the proposed drive system can operate at zero/low frequency under rated load torque; 2) the MMC in the proposed drive system operates at medium frequency, which requires smaller SM capacitance compared to variable dc voltage methods [15]-[21]; 3) the device current

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stress in the MMC with proposed method is much less than that with current injection based methods [10]-[14].

The rest of paper is organized as follows. Section II proposes the cascaded MMC and CCV based machine drive system. Section III proposes operating principles. Section IV discusses the proposed system. Sections V and VI present the simulation and experiment, respectively. Section VII gives conclusion.

## II. PROPOSED CASCADED MMC AND CCV BASED MACHINE DRIVE SYSTEM

### A. Proposed Drive System

A cascaded MMC and CCV based machine drive system is proposed, as shown in Fig. 1. The MMC operates as the grid-side converter, and the CCV operates as the machine-side converter. The MMC is connected to the dc grid and provides the ac voltage with medium-frequency  $f_g$  for the CCV. The CCV converts the input medium-frequency ac voltage to the required ac voltage with low-frequency  $f_m$  to drive the permanent magnet synchronous machine (PMSM).

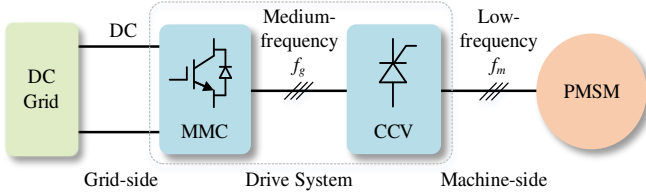


Fig. 1. Block diagram of proposed machine drive system.

### B. MMC Based Grid-Side Converter

Fig. 2(a) shows the grid-side three-phase MMC, whose each phase includes an upper arm, a lower arm, a filter inductor  $L_f$ , and a compensation capacitor  $C_{com}$ . Each arm consists of  $n$  identical SMs and an arm inductor  $L_s$ . Fig. 2(b) shows a SM, which consists of the switch/diode  $T_1/D_1$ ,  $T_2/D_2$  and a dc capacitor  $C_{sm}$ .

According to [5], in the MMC, the output voltage  $u_j$  in phase  $j$  ( $j=a, b, c$ ) can be expressed as

$$u_j = \frac{u_{uj} - u_{lj}}{2} - L \frac{di_j}{dt} \quad (1)$$

with

$$L = \frac{L_s}{2} + L_f \quad (2)$$

where  $u_{uj}$  and  $u_{lj}$  are the total SM output voltage of the upper arm and lower arm in phase  $j$ , respectively.  $i_j$  is the ac-side current of phase  $j$ .  $L$  is the equivalent output inductance of the MMC.

### C. CCV Based Machine-Side Converter

Fig. 3 shows the machine-side three-pulse half-wave CCV. The CCV consists of three phase units. Each phase unit contains three pairs of inverse parallel thyristors including  $Th_{p1}$  &  $Th_{n1}$ ,  $Th_{p2}$  &  $Th_{n2}$ , and  $Th_{p3}$  &  $Th_{n3}$ , where the thyristors  $Th_{p1}$ - $Th_{p3}$  constitute a positive converter and the thyristors  $Th_{n1}$ - $Th_{n3}$  constitute a negative converter.  $L_T$  is the commutation inductor.

Taking phase unit  $a$  for example and neglecting harmonics, Fig. 4 shows the fundamental components of the output voltage

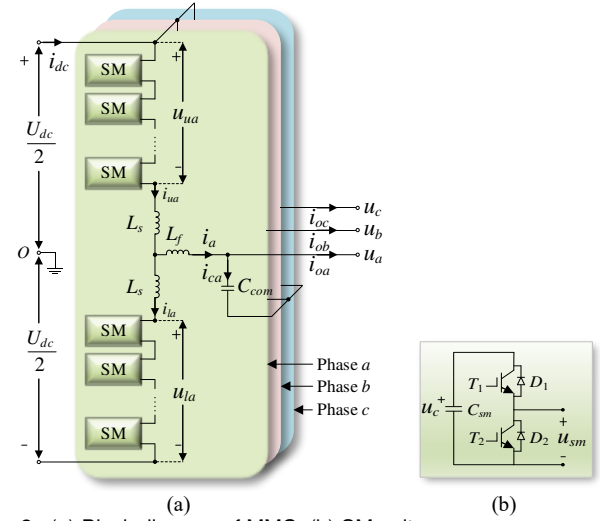


Fig. 2. (a) Block diagram of MMC. (b) SM unit.

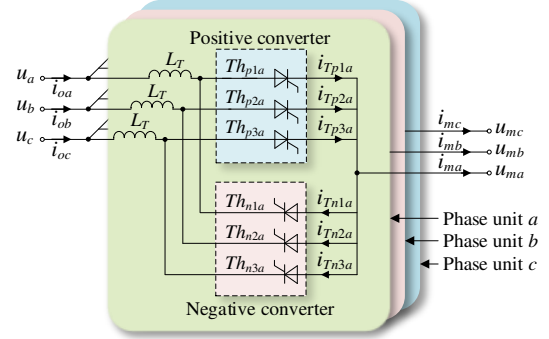


Fig. 3. Block diagram of the CCV.

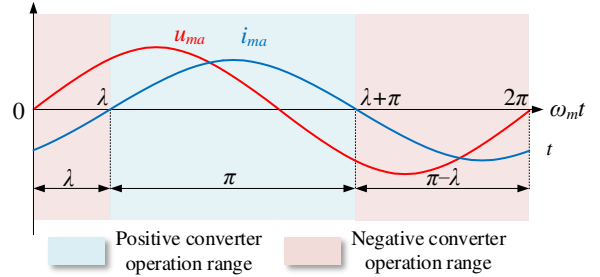


Fig. 4. Fundamental frequency components of the CCV's output.

$u_{ma}$  and current  $i_{ma}$  of the CCV, which can be expressed as

$$u_{ma} = U_m \sin(\omega_m t) \quad (3)$$

$$i_{ma} = I_m \sin(\omega_m t - \lambda) \quad (4)$$

where  $U_m$  and  $I_m$  are the amplitudes of the machine phase voltage and current, respectively.  $\omega_m$  is the fundamental angular frequency.  $\lambda$  is the lagging displacement angle of machine, which decides the operation of the positive converter and negative converter, as follows.

- $\omega_m t \in [\lambda, \lambda + \pi]$ :  $i_{ma}$  is positive and the positive converter ( $Th_{p1a}$ ,  $Th_{p2a}$ ,  $Th_{p3a}$ ) works.
- $\omega_m t \in [0, \lambda] \text{ \& } [\lambda + \pi, 2\pi]$ :  $i_{ma}$  is negative and the negative converter ( $Th_{n1a}$ ,  $Th_{n2a}$ ,  $Th_{n3a}$ ) works.

The  $Th_{p1a}$ ,  $Th_{p2a}$ ,  $Th_{p3a}$  in the positive converter or the  $Th_{n1a}$ ,  $Th_{n2a}$ ,  $Th_{n3a}$  in the negative converter are fired alternately, and only one thyristor is conducting simultaneously, where the thyristor's firing angle  $\alpha$  can be obtained based on the cosine

wave crossing method [23], as

$$\alpha = \arccos(y_{ref\_ma}) \quad (5)$$

with

$$y_{ref\_ma} = r \cdot \sin(\omega_m t) \quad (6)$$

where  $y_{ref\_ma}$  is the reference for phase  $a$  of the CCV.  $r$  is modulation index with  $0 \leq r \leq 1$ .

### III. CONTROL OF PROPOSED MACHINE DRIVE SYSTEM

#### A. Control of Grid-Side MMC

The MMC provides a constant medium-frequency ac output voltage for the CCV. The control structure of the MMC is shown in Fig. 5(a), including the output voltage control and circulating current suppression control (CCSC) [24]. Fig. 5(b) shows the output voltage control in detail, which adopts double-loop vector control to ensure a constant output voltage of the MMC.  $u_d$ ,  $u_q$  and  $i_{od}$ ,  $i_{oq}$  are the  $dq$ -axis components of output voltages  $u_a$ ,  $u_b$ ,  $u_c$  and output currents  $i_{oa}$ ,  $i_{ob}$ ,  $i_{oc}$ , respectively.  $i_d$ ,  $i_q$  are the  $dq$ -axis components of ac-side currents  $i_a$ ,  $i_b$ ,  $i_c$ .  $\omega_g$  is the angular frequency of output voltage and  $\omega_g = 2\pi f_g$ , where  $f_g$  is the MMC's output frequency.  $U_{dc}$  is the dc-side voltage of the MMC. According to the voltage commands  $u_d^*$  and  $u_q^*$ , where  $u_d^*$  is equal to the amplitude of MMC's phase voltage and  $u_q^*$  is 0, the outer loop generates the current commands  $i_d^*$  and  $i_q^*$ . The inner loop produces the  $dq$ -axis reference voltages  $u_{ref\_d}$  and  $u_{ref\_q}$ . And then, the reference voltage  $u_{ref\_j}$  for phase  $j$  is derived by the inverse  $dq$  transformation. Fig. 5(c) shows the CCSC in detail,  $i_{uj}$  and  $i_{lj}$  are the upper and lower arm currents in phase  $j$ , respectively.  $i_{cir\_d}$  and  $i_{cir\_q}$  are the  $dq$ -axis components of circulating currents, respectively. The CCSC produces the  $dq$ -axis reference voltages  $u_{cir\_d}$  and  $u_{cir\_q}$ , then the reference voltage  $u_{cir\_j}$  for phase  $j$  is derived by the inverse  $dq$  transformation. Finally, the upper arm reference voltage and lower arm reference voltage can be obtained as  $u_{ref\_uj} = (u_{cir\_j} - u_{ref\_j})$  and  $u_{ref\_lj} = (u_{cir\_j} + u_{ref\_j})$ , where the  $u_{cir\_j}$  is the reference for phase  $j$  produced by the CCSC, as shown in Fig. 5(a). Finally, the upper arm reference and lower arm reference signals can be obtained as

$$\begin{cases} y_{ref\_uj} = 2u_{ref\_uj}/U_{dc} \\ y_{ref\_lj} = 2u_{ref\_lj}/U_{dc} \end{cases} \quad (7)$$

which are used for the upper arm and the lower arm in phase  $j$  of the MMC, respectively.

#### B. Control of Machine-Side CCV

The CCV is employed to control the machine and Fig. 6 shows the vector control of the CCV.  $i_{md}$ ,  $i_{mq}$  and  $L_{md}$ ,  $L_{mq}$  are the  $dq$ -axis components of machine currents and inductances, respectively.  $\psi$  is the permanent magnet flux linkage.  $\theta$  is the electrical rotor position angle of the machine. According to the command  $\omega_m^*$ , the outer loop produces the  $q$ -axis current command  $i_{mq}^*$ . The  $d$ -axis current command  $i_{md}^*$  is 0. The inner loop produces the  $dq$ -axis reference voltages  $u_{ref\_md}$  and  $u_{ref\_mq}$  to make the current  $i_{md}$  and  $i_{mq}$  follow their commands, and then three-phase reference voltage  $u_{ref\_mj}$  is derived from the inverse  $dq$  transformation. According to [23], the relationship among

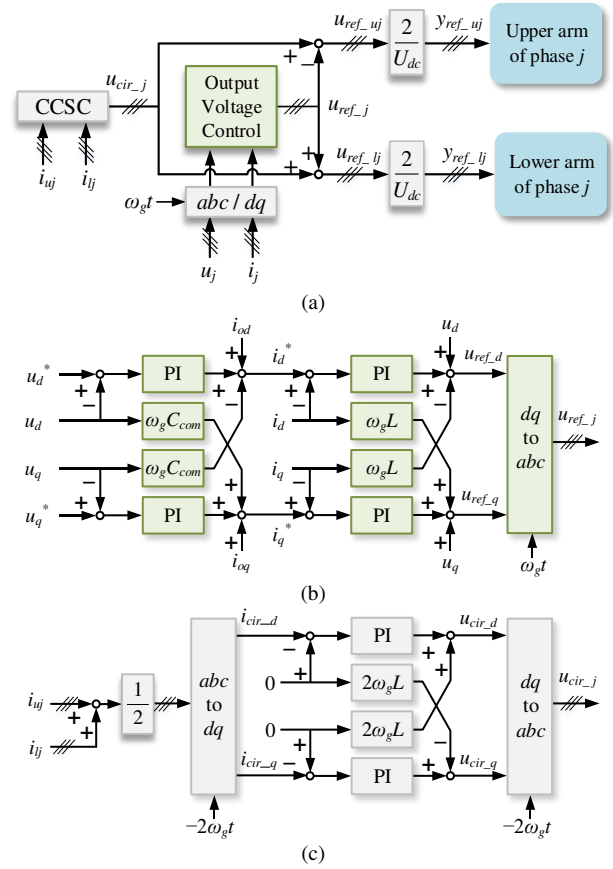


Fig. 5. (a) Overall control diagram of the grid-side MMC. (b) Output voltage control diagram of the MMC. (c) Circulating current suppression control diagram of the MMC.

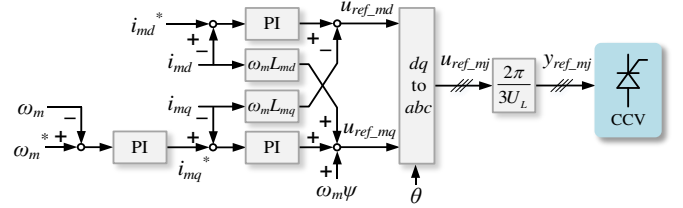


Fig. 6. Control diagram of the CCV.

CCV's input phase voltage amplitude  $U_p$ , output phase voltage amplitude  $U_m$ , and modulation index  $r$  is

$$r = \frac{2\pi U_m}{3\sqrt{3}U_p} \quad (8)$$

Substituting (8) into (6), the reference signal  $y_{ref\_mj}$  can be derived as

$$y_{ref\_mj} = \frac{2\pi}{3\sqrt{3}U_p} u_{ref\_mj} = \frac{2\pi}{3U_L} u_{ref\_mj} \quad (9)$$

where  $U_L$  is the CCV's input line voltages  $u_{ab}$ ,  $u_{bc}$ ,  $u_{ca}$ . The  $y_{ref\_mj}$  is used for the CCV to control the machine.

### IV. DISCUSSION OF PROPOSED DRIVE SYSTEM

#### A. Studied Drive System

In this paper, a 6.6 kV/5 MW low-speed PMSM based drive system is studied, which is normally operated at the rated situation in applications such as conveyor. The system parameters are shown in Table I.

| Parameter |                                    | Value |
|-----------|------------------------------------|-------|
| PMSM      | Rated stator rms line voltage (kV) | 6.6   |
|           | Rated rms current (A)              | 462   |
|           | Number of pole pairs               | 12    |
|           | Rated speed (r/min)                | 50    |
|           | Rated frequency (Hz)               | 10    |
|           | Rated displacement factor          | 0.95  |
| MMC       | DC grid voltage (kV)               | 20    |
|           | Rated rms line voltage (kV)        | 8.9   |
|           | Rated frequency (Hz)               | 100   |
|           | SM number per arm $n$              | 12    |
|           | SM capacitance (mF)                | 2.76  |
|           | Arm inductance (mH)                | 3     |
| CCV       | Compensation capacitance (mF)      | 0.1   |
|           | Carrier frequency (kHz)            | 1     |
| CCV       | Commutation inductance (mH)        | 0.63  |

### B. Commutation Inductor $L_T$ of CCV

The commutation inductor  $L_T$ , as shown in Fig. 3, is adopted to limit the rising rate of the CCV's thyristor current during commutation between the thyristors. Taking the commutation in the positive converter of phase unit  $a$  as an example, Fig. 7 shows the commutation from outgoing thyristor  $Th_{p3a}$  to incoming thyristor  $Th_{p1a}$  in the commutation period  $\mu$ , where the  $Th_{p3a}$ 's current  $i_{Tp3a}$  is gradually reduced, the  $Th_{p1a}$ 's current  $i_{Tp1a}$  is gradually increased, and the  $I_T = i_{Tp1a} + i_{Tp3a}$  is nearly a constant. According to (4) and (5), the  $I_T$  can be obtained as

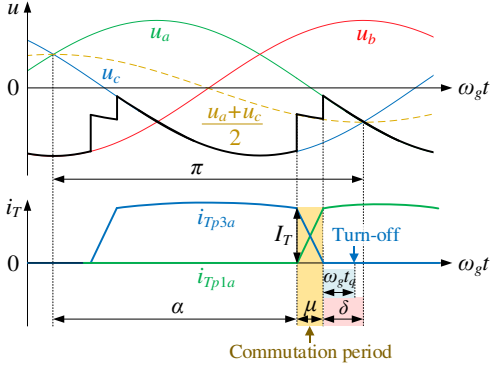


Fig. 7. Commutation from  $Th_{p3a}$  to  $Th_{p1a}$ .

$$I_T = I_m \sin \left[ \arcsin \left( \frac{\cos \alpha}{r} \right) - \lambda \right] \quad (10)$$

The rising rate of the thyristor current  $i_T$  during commutation period  $\mu$  is

$$\frac{di_T}{dt} = 2\pi f_g \cdot \frac{I_T}{\mu} \quad (11)$$

with

$$\mu = \arccos \left( \cos \alpha - \frac{4\pi f_g L_T I_T}{U_L} \right) - \alpha \quad (12)$$

It can be observed that along with the increase of the

commutation inductor  $L_T$ , the  $di_T/dt$  will reduce; along with the reduction of  $L_T$ , the  $di_T/dt$  will increase.

Normally, the maximum  $di_T/dt$  appears when the CCV works at the rated situation. According to (10) and (11), the  $di_T/dt$  is related to  $\alpha$  for the given  $L_T$  and  $f_g$ . Fig. 8(a) shows the range of  $\alpha$  for the positive converter in phase unit  $a$  under various phase angle  $\omega_m t$  of  $u_{ma}$ , which is derived from Table I. Fig. 8(b) shows the  $di_T/dt$  under various phase angles  $\omega_m t$  of  $u_a$  and various  $f_g$ , where  $L_T = 0.63$  mH. It can be observed that the  $di_T/dt$  reaches its minimum value when phase angle  $\omega_m t$  is close to  $\pi/2$ , and the  $di_T/dt$  increases when the  $\omega_m t$  is far from  $\pi/2$ . The maximum  $di_T/dt$  under various  $f_g$  are all close to 10 A/ $\mu$ s. Taking the thyristor Infineon T2871N [25] as an example, whose nominal  $di_T/dt$  is 10 A/ $\mu$ s. In order to ensure that the maximum  $di_T/dt$  does not exceed the nominal value,  $L_T$  should be more than 0.63 mH.

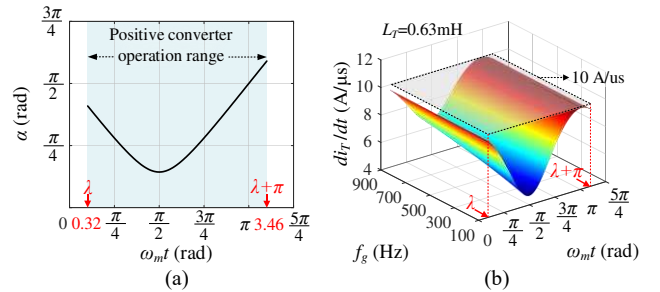


Fig. 8. (a) The change of  $\alpha$  in the operation range of positive converter. (b)  $di_T/dt$  under various  $f_g$  when  $L_T = 0.63$  mH.

### C. Operation Frequency $f_g$ of MMCs

In Fig. 7, the extinction angle  $\delta$  is

$$\delta = \pi - (\alpha + \mu) \quad (13)$$

The extinction time  $t_\delta$  is

$$t_\delta = \frac{\delta}{2\pi} \cdot \frac{1}{f_g} \quad (14)$$

According to (13) and (14), it can be observed that along with the increase of  $(\alpha + \mu)$  and  $f_g$ , the  $t_\delta$  will reduce, which is critical for the commutation. According to (5) and (12),  $(\alpha + \mu)$  can reach the maximum at rated power, which will result in the minimum  $\delta$ . Taking the positive converter in phase unit  $a$  as an example, and according to (14), Fig. 9(a) shows the  $t_\delta$  in the operation range of positive converter under rated situation, where various  $f_g$  are considered. Based on Fig. 9(a), the minimum extinction time  $t_{\delta\_min}$  under various  $f_g$  can be obtained, as shown in Fig. 9(b). Along with the increase of  $f_g$ , the  $t_{\delta\_min}$  will reduce, and vice versa.

In order to avoid commutation failure, the minimum  $t_{\delta\_min}$  of the thyristor must be more than the thyristor's turn-off time  $t_q$ . As a result, according to Fig. 9(b), the maximum  $f_g$  should meet

$$f_{g\_max} \leq f_g |_{(t_{\delta\_min} = t_q)} \quad (15)$$

The minimum  $f_g$  of CCV is limited by its output frequency  $f_m$ . Referring to [26], the minimum  $f_g$  in three-pulse half-wave CCV should be

$$f_{g\_min} \geq 6f_m \quad (16)$$



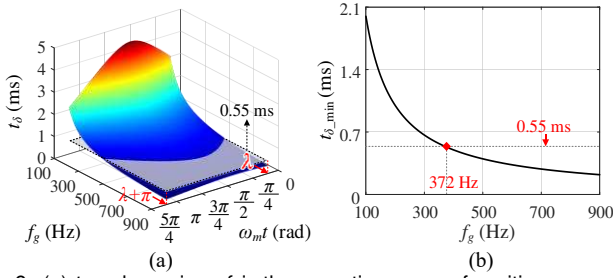


Fig. 9. (a)  $t_g$  under various  $f_g$  in the operation range of positive converter. (b)  $t_{g\_min}$  under various  $f_g$ .

For the system in Table I, the thyristor Infineon T2871N [25] is considered, whose  $t_q$  is 0.55 ms. According to Fig. 9(b) and (15), there is  $f_{g\_max} \leq 372$  Hz. The rated frequency  $f_m$  of the machine is 10 Hz. According to (16), there is  $f_{g\_min} \geq 60$  Hz. Although a higher  $f_g$  brings smoother output current, it requires higher sampling frequency. Here, the rated  $f_g$  is set as 100 Hz.

#### D. Compensation Capacitor $C_{com}$ of MMCs

A compensation capacitor  $C_{com}$ , as shown in Fig. 2, is adopted in the MMC, whose capacitive reactive power is

$$Q_{NC} = \frac{1}{2} \omega_g C_{com} U_L^2 \quad (17)$$

The  $C_{com}$  is used to compensate the inductive reactive power  $Q_{NV}$  of the CCV at rated situation, which is caused by the CCV and results in the lagging displacement angle  $\varphi_N$  between the CCV's input currents  $i_{oa}$ ,  $i_{ob}$ ,  $i_{oc}$  and phase voltages  $u_a$ ,  $u_b$ ,  $u_c$ . Here, the inductive reactive power  $Q_{NV}$  of the CCV at rated can be calculated as

$$Q_{NV} = P_{NV} \tan \varphi_N \quad (18)$$

where  $P_{NV}$  is the rated power at the input side of the CCV. Neglecting the power loss in the CCV, the  $P_{NV}$  equals to the rated power at the ac side of the machine as

$$P_{NV} = \frac{3}{2} U_{mN} I_{mN} \cos \lambda \quad (19)$$

where  $U_{mN}$  and  $I_{mN}$  are the amplitude of machine's rated phase voltage and current, respectively.

According to (17)~(18), the  $C_{com}$  can be obtained as

$$C_{com} = \frac{2 P_{NV} \tan \varphi_N}{\omega_g U_L^2} \quad (20)$$

Substituting Table I into (20), the  $C_{com}$  in the system can be obtained as 0.1 mF.

#### E. Device Current Stress of MMCs

Suppose that the circulating current in the MMC is suppressed by the CCSC, the upper arm current  $i_{uj}$  and the lower arm current  $i_{lj}$  in phase  $j$  of the MMC, as shown in Fig. 2, can be expressed as

$$\begin{cases} i_{uj} = \frac{i_{dc}}{3} + \frac{i_j}{2} \\ i_{lj} = \frac{i_{dc}}{3} - \frac{i_j}{2} \end{cases} \quad (21)$$

where  $i_{dc}$  is the dc current. The ac-side current  $i_j$  in phase  $j$  is

$$i_j = i_{cj} + i_{oj} \quad (22)$$

with

$$i_{cj} = C_{com} \frac{du_j}{dt} \quad (23)$$

where  $i_{cj}$  is the compensation capacitor current, which mainly consists of the fundamental-frequency component.  $i_{oj}$  is the output current in phase  $j$ .

Due to the CCV, the MMC's output current  $i_{oj}$  contains fundamental-frequency component and harmonic components. Fig. 10(a) shows the frequency spectrum of  $i_{oj}$  at rated situation, which is derived from the system in Table I. It can be observed that the frequencies of the harmonics mainly include  $2f_g \pm 3f_m$ ,  $4f_g \pm 3f_m$ ,  $5f_g$  &  $5f_g \pm 6f_m$ ,  $7f_g$  &  $7f_g - 6f_m$ . Fig. 10(b) shows the frequency spectrum of  $i_j$  at rated situation, whose harmonics are almost the same to those in  $i_{oj}$ , as shown in Fig. 10(a). The amplitude of fundamental component in Fig. 10(b) is less than that in Fig. 10(a), because its reactive component is compensated by  $C_{com}$ .

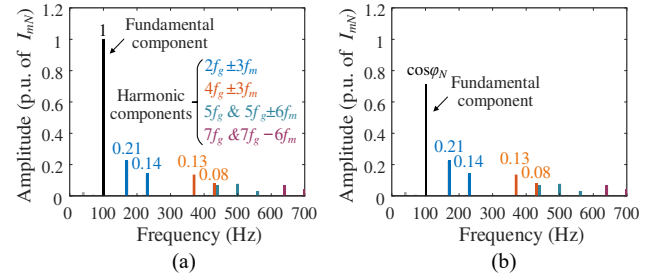


Fig. 10. (a) Frequency spectrum of  $i_{oj}$  at rated situation. (b) Frequency spectrum of  $i_j$  at rated situation.

Fig. 11 shows the peak value of MMC's arm currents under various machine speeds, which is derived from the system in Table I. It can be seen that along with the increase of machine speed, the current peak value also increases. Fig. 11 also shows the current peak value of the MMC based machine drive system with square-wave circulating current injection method [11], whose current peak value is the minimum among various circulating current injection methods. It can be observed that the device current stress in the proposed machine drive system is much lower than that in the circulating current injection method, because the proposed method does not need to inject high-amplitude circulating currents.

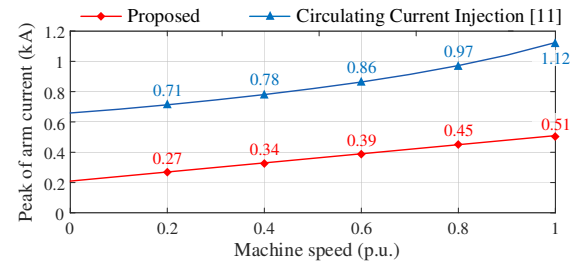


Fig. 11. Comparison of arm current peak value between proposed method and current injection method [11].

#### F. SM Capacitor $C_{sm}$ of MMCs

Taking the upper arm of phase  $a$  for example, according to (21) and Fig. 10(b), the rated arm current  $i_{uaN}$  can be simplified

$$\begin{aligned}\Delta u_{cuaN} &= \frac{1}{C_{sm}} \int i_{cuaN} dt = \frac{m i_{dcN} \cos(\omega_g t)}{6 \omega_g C_{sm}} - \frac{I_{mN}}{4 C_{sm} \omega_g} \left\{ \cos \varphi_N \cos(\omega_g t) + \frac{m \cos \varphi_N \sin(2 \omega_g t)}{4} \right\} \\ &= -\frac{I_{mN}}{4 C_{sm}} \left\{ \frac{k_{4n}}{\omega_{4n}} \cos(\omega_{4n} t + \varphi_{4n}) + \frac{k_{4p}}{\omega_{4p}} \cos(\omega_{4p} t + \varphi_{4p}) + \frac{k_{2p}}{\omega_{2p}} \cos(\omega_{2p} t + \varphi_{2p}) + \frac{k_{2n}}{\omega_{2n}} \cos(\omega_{2n} t + \varphi_{2n}) \right\} \\ &\quad + \frac{m I_{mN}}{8 C_{sm}} \left\{ \frac{k_{2n} \sin[(\omega_{2n} + \omega_g) t + \varphi_{2n}]}{(\omega_{2n} + \omega_g)} - \frac{k_{2n} \sin[(\omega_{2n} - \omega_g) t + \varphi_{2n}]}{(\omega_{2n} - \omega_g)} + \frac{k_{2p} \sin[(\omega_{2p} + \omega_g) t + \varphi_{2p}]}{(\omega_{2p} + \omega_g)} - \frac{k_{2p} \sin[(\omega_{2p} - \omega_g) t + \varphi_{2p}]}{(\omega_{2p} - \omega_g)} \right. \\ &\quad \left. + \frac{k_{4n} \sin[(\omega_{4n} + \omega_g) t + \varphi_{4n}]}{(\omega_{4n} + \omega_g)} - \frac{k_{4n} \sin[(\omega_{4n} - \omega_g) t + \varphi_{4n}]}{(\omega_{4n} - \omega_g)} + \frac{k_{4p} \sin[(\omega_{4p} + \omega_g) t + \varphi_{4p}]}{(\omega_{4p} + \omega_g)} - \frac{k_{4p} \sin[(\omega_{4p} - \omega_g) t + \varphi_{4p}]}{(\omega_{4p} - \omega_g)} \right\}\end{aligned}\quad (26)$$

as (24), where only the fundamental component and harmonic components  $2f_g \pm 3f_m$  and  $4f_g \pm 3f_m$  are considered.

$$\begin{aligned}i_{uaN} &= \frac{i_{dcN}}{3} + \frac{i_{aN}}{2} \\ &= \frac{i_{dcN}}{3} + \frac{1}{2} I_{mN} \cos \varphi_N \sin(\omega_g t) \\ &\quad + \frac{1}{2} I_{mN} [k_{2n} \sin(\omega_{2n} t + \varphi_{2n}) + k_{2p} \sin(\omega_{2p} t + \varphi_{2p})] \\ &\quad + \frac{1}{2} I_{mN} [k_{4n} \sin(\omega_{4n} t + \varphi_{4n}) + k_{4p} \sin(\omega_{4p} t + \varphi_{4p})]\end{aligned}\quad (24)$$

where  $i_{dcN}$  is rated dc current.  $i_{aN}$  is the rated ac-side current of phase  $a$ .  $k_{2n}$ ,  $k_{2p}$ ,  $k_{4n}$ ,  $k_{4p}$  are respectively the p.u. values of harmonics  $2f_g - 3f_m$ ,  $2f_g + 3f_m$ ,  $4f_g - 3f_m$  and  $4f_g + 3f_m$  as shown in Fig. 10(b).  $\omega_{2n}$ ,  $\omega_{2p}$ ,  $\omega_{4n}$ ,  $\omega_{4p}$  are respectively the angular frequency of these harmonics.  $\varphi_{2n}$ ,  $\varphi_{2p}$ ,  $\varphi_{4n}$ ,  $\varphi_{4p}$  are respectively the phase angles of these harmonics.

According to [27], the SM capacitor current in upper arm of phase  $a$  can be expressed as

$$i_{cuaN} = \frac{1 - y_{ref\_ua}}{2} \cdot i_{uaN} \quad (25)$$

Normally, the circulating current control has little effect on the  $y_{ref\_ua}$  [28]. Therefore, it can be expressed as  $y_{ref\_ua} = m \cdot \sin(\omega_g t)$ , where  $m$  is the modulation index of MMC. Combining (24) and (25), the rated capacitor voltage fluctuation  $\Delta u_{cuaN}$  can be obtained as (26).

The SM capacitor voltage fluctuation ratio  $\varepsilon$  can be defined as

$$\varepsilon = \frac{\text{Max}[\Delta u_{cuaN}]}{U_{dc} / n} \quad (27)$$

Fig. 12 shows the relationship between  $\varepsilon$  and  $C_{sm}$  in the MMC of the proposed system, which is derived from (24)~(27) and Table I. It can be seen that along with the increase of  $C_{sm}$ ,  $\varepsilon$  will be reduced; along with the reduction of  $C_{sm}$ ,  $\varepsilon$  will be increased. Fig. 12 also shows relationship between the  $\varepsilon$  and  $C_{sm}$  in the HMMC based machine drive system [15]. It can be observed

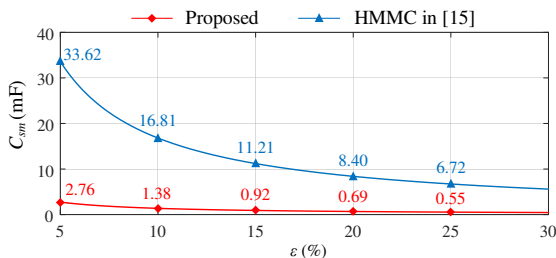


Fig. 12. Comparison of SM capacitance between MMC in proposed system and HMMC [15].

that for the same capacitor voltage fluctuation, the required capacitance in the proposed machine drive system is far less than that in the HMMC based machine drive system. According to Fig. 12, the  $C_{sm}$  of 2.76 mF corresponding to the capacitor voltage fluctuation of 2% is selected in the proposed system.

## V. SIMULATION STUDIES

To verify the proposed machine drive system, the system simulation is conducted with professional tool PLECS. The system diagram is shown in Fig. 1 and the system parameters are shown in Table I.

### A. Performance of proposed system

Fig. 13 shows the performance of the proposed machine drive system, where the machine operates under rated load from standstill to the rated speed. Fig. 13(a) shows the machine speed. The machine accelerates at 1s from standstill to 0.5 p.u. speed and accelerates at 2.5s from 0.5 p.u. to rated speed. Fig. 13(b) shows the machine line voltage. Fig. 13(c) shows the machine currents, whose frequency changes from 0 to 10 Hz. Fig. 13(d) shows the electrical torque. The torque ripple increases with the speed and reaches the maximum value 0.10 p.u. at rated situation. Fig. 13(e) shows the line voltages of the MMC, whose frequency  $f_g$  is 100 Hz. Fig. 13(f) shows the output current of the MMC. Fig. 13(g) shows the MMC's arm currents, whose peak value rises with the increase of the machine speed. The peak of arm current is 514 A. Fig. 13(h) shows the SM capacitor voltages of upper and lower arm in phase  $a$  of MMC. The voltage fluctuation rises with the arm current, ranging from 1590 to 1749 V at the rated speed. The voltage fluctuation ratio is less than 5% when the  $C_{sm}$  is 2.76 mF, which verifies the analysis in Fig. 12.

Fig. 14 shows the harmonic spectrums of machine line voltage and current at rated situation. It can be observed that the main harmonic components of machine voltage are in the sidebands of  $3f_g$  and  $6f_g$ . The main harmonic components of machine current are in the sidebands of  $3f_g$ .

### B. Comparison with traditional MMC

Fig. 15 shows the comparison of capacitor voltages between traditional MMC based drive system and proposed system, where the SM capacitance of traditional MMC is 7 times (19.32 mF) of proposed system (2.76 mF). Fig. 15(a) and (b) show the capacitor voltage fluctuation at 0.2 p.u. speed under rated load. Fig. 15(c) and (d) show the capacitor voltage fluctuation at rated situation. It can be observed that the voltage fluctuation of

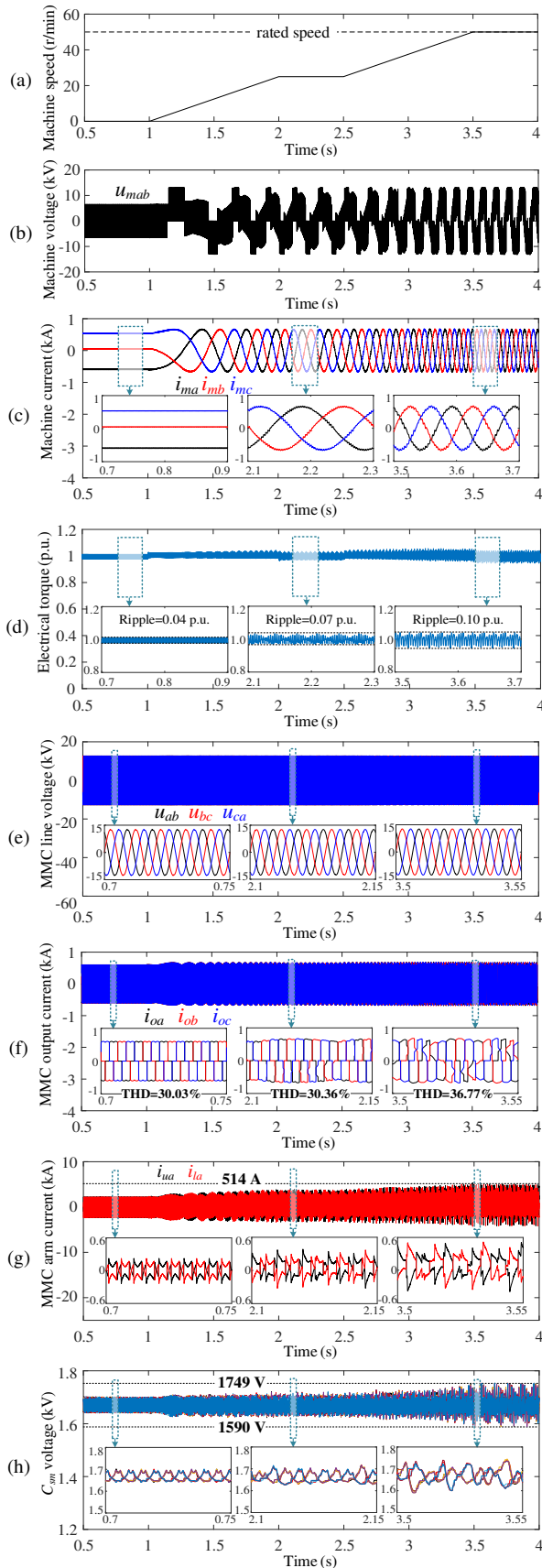


Fig. 13. Simulation waveforms. (a) Machine speed. (b) Machine line voltage. (c) Machine currents. (d) Electrical torque. (e) MMC line voltages. (f) MMC output currents. (g) Arm currents of phase a. (h) SM capacitor voltages of phase a.

traditional MMC increases as machine speed reduces, which is 42.88% at 0.2 p.u. speed. Compared to traditional MMC, proposed system can operate stably at low speed with lower SM capacitance, and the voltage fluctuation is less than 5% in the whole speed range.

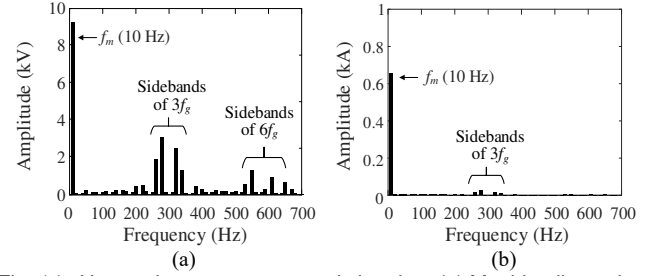


Fig. 14. Harmonic spectrum at rated situation. (a) Machine line voltage. (b) Machine current.

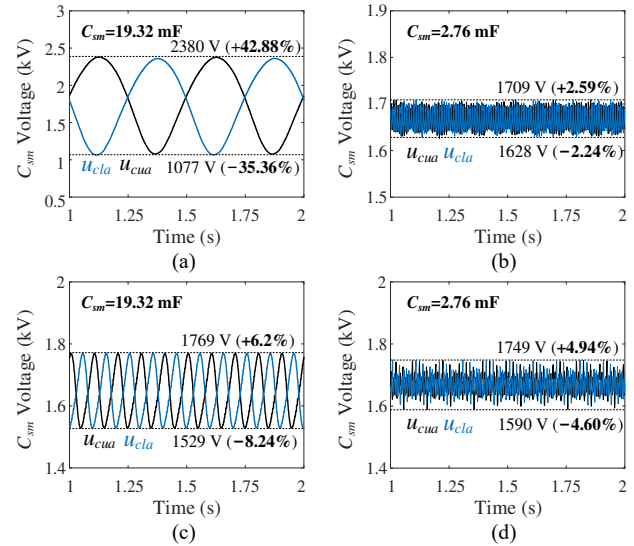


Fig. 15. Comparison of capacitor voltage fluctuation. (a) Traditional MMC at 0.2 p.u. speed. (b) Proposed system at 0.2 p.u. speed. (c) Traditional MMC at rated speed. (d) Proposed system at rated speed.

## VI. EXPERIMENTAL STUDIES

A prototype of the proposed machine drive system is built in the lab, as shown in Fig. 16. A dc power supply is used to support the dc voltage. The ac side of the MMC is connected to the CCV. The output side of CCV is connected to the PMSM. The control algorithm is implemented by digital signal processor (DSP) and the drive signals are transferred to driving circuit of each device by optical fibers. The system parameters are listed in Table II.

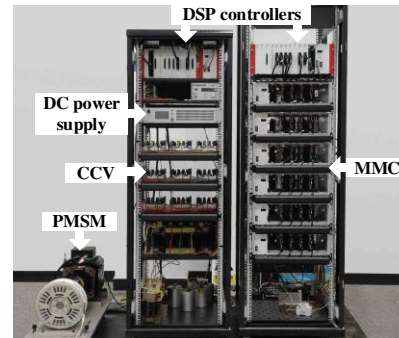


Fig. 16. Photo of experimental platform.



TABLE II  
PARAMETERS OF EXPERIMENTAL SYSTEM

| Parameter |                                   | Value |
|-----------|-----------------------------------|-------|
| PMSM      | Rated stator rms line voltage (V) | 44    |
|           | Rated rms current (A)             | 5.66  |
|           | Number of pole pairs              | 4     |
|           | Rated speed (r/min)               | 150   |
|           | Rated frequency (Hz)              | 10    |
|           | Rated displacement factor         | 0.95  |
| MMC       | DC voltage (V)                    | 140   |
|           | Rated rms line voltage (V)        | 62    |
|           | Rated frequency (Hz)              | 100   |
|           | SM number per arm $n$             | 4     |
|           | SM capacitance (mF)               | 2.7   |
|           | Arm inductance (mH)               | 0.5   |
| CCV       | Compensation capacitance (mF)     | 0.18  |
|           | Carrier frequency (kHz)           | 5     |
|           | Commutation inductance (mH)       | 1     |

### A. Steady State Operation

Fig. 17 shows the shows the line voltages of the MMC, whose frequency is 100Hz. Fig. 18 shows the steady state operation at standstill under rated load. Fig. 19 shows the steady state operation at 0.5 p.u. speed under rated load. Fig. 20 shows the steady state operation at rated speed under 0.5 p.u. load. Fig. 21 shows the steady state operation at rated speed under rated load.

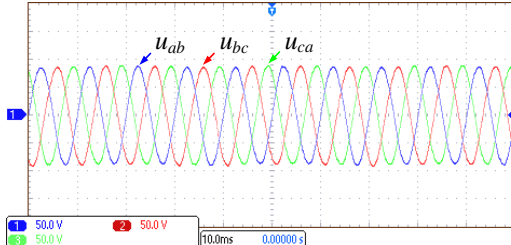


Fig. 17. Experimental waveforms of  $u_{ab}$ ,  $u_{bc}$ ,  $u_{ca}$  (50 V/div).

Fig. 18(a), Fig. 19(a), Fig. 20(a) and Fig. 21(a) show the machine voltages  $u_{mab}$ ,  $u_{mbc}$ ,  $u_{mca}$ . Fig. 18(b), Fig. 19(b), Fig. 20(b) and Fig. 21(b) show the machine currents  $i_{ma}$ ,  $i_{mb}$ ,  $i_{mc}$ . Under rated load in Figs. 19~20, the fundamental frequency machine current amplitude is 8 A. Under 0.5 p.u. load in Fig. 21, the fundamental frequency machine current amplitude is 4 A. Fig. 18(c), Fig. 19(c), Fig. 20(c) and Fig. 21(c) show the spectrum of machine line voltage, where the main harmonic components are in the sidebands of  $3f_g$  and  $6f_g$ . Fig. 18(d), Fig. 19(d), Fig. 20(d) and Fig. 21(d) show the spectrum of machine current, where the main harmonic components are in the sidebands of  $3f_g$ . Fig. 18(e), Fig. 19(e), Fig. 20(e) and Fig. 21(e) show the MMC's output current  $i_{oa}$ ,  $i_{ob}$ ,  $i_{oc}$ , whose THD reaches the maximum 34.06% at rated situation. Fig. 18(f), Fig. 19(f), Fig. 20(f) and Fig. 21(f) show the arm currents and the SM capacitor voltages in phase  $a$  of the MMC. It can be observed that the peak of arm current increases as the machine speed and torque increase. At rated situation, the peak of arm current

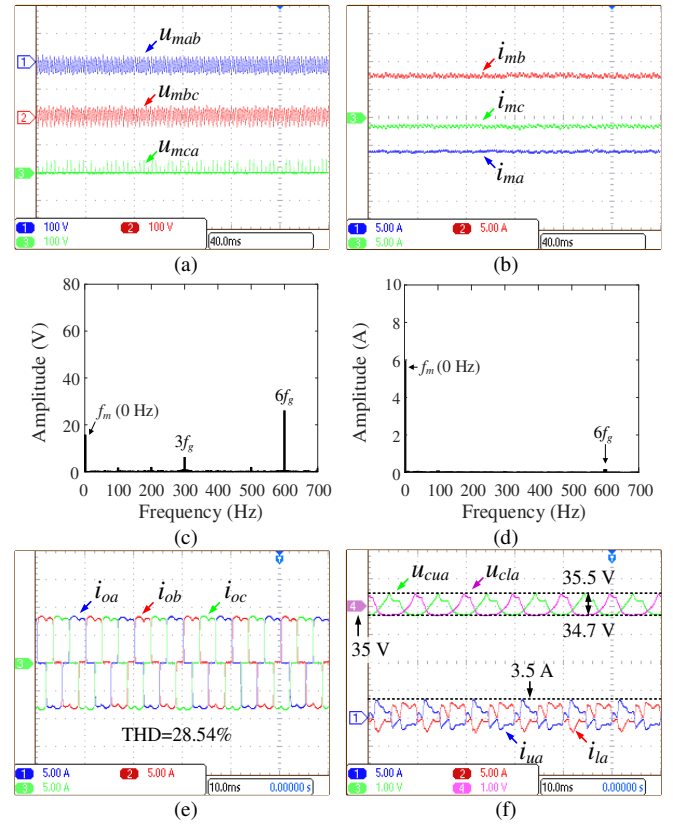


Fig. 18. Experimental waveforms at standstill. (a)  $u_{mab}$ ,  $u_{mbc}$ ,  $u_{mca}$  (100 V/div). (b)  $i_{ma}$ ,  $i_{mb}$ ,  $i_{mc}$  (5 A/div). (c) Spectrum of  $u_{mab}$ . (d) Spectrum of  $i_{ma}$ . (e)  $i_{oa}$ ,  $i_{ob}$ ,  $i_{oc}$  (5 A/div). (f)  $i_{ua}$ ,  $i_{la}$  (5 A/div),  $u_{cua}$ ,  $u_{cla}$  (1 V/div).

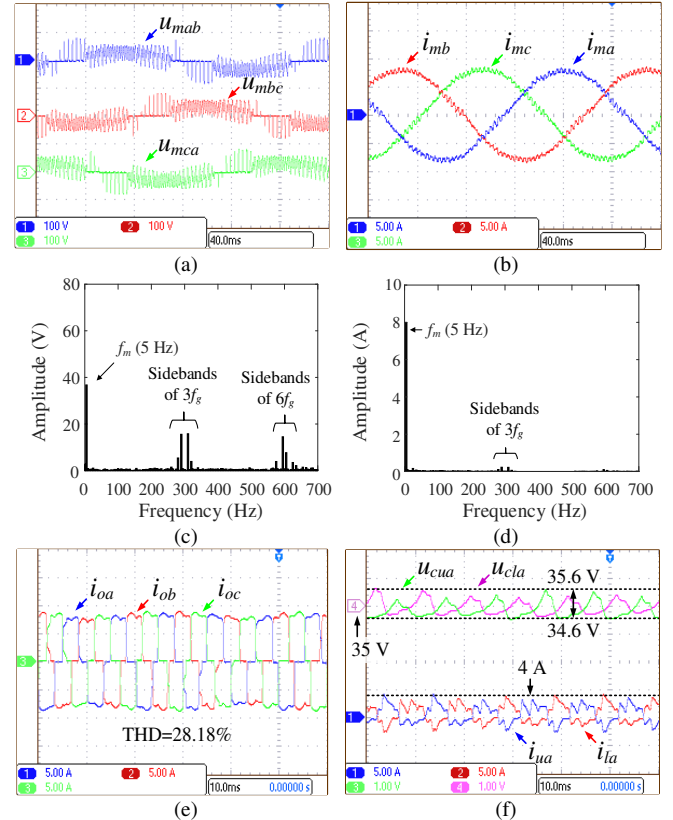


Fig. 19. Experimental waveforms at 0.5 p.u. speed. (a)  $u_{mab}$ ,  $u_{mbc}$ ,  $u_{mca}$  (100 V/div). (b)  $i_{ma}$ ,  $i_{mb}$ ,  $i_{mc}$  (5 A/div). (c) Spectrum of  $u_{mab}$ . (d) Spectrum of  $i_{ma}$ . (e)  $i_{oa}$ ,  $i_{ob}$ ,  $i_{oc}$  (5 A/div). (f)  $i_{ua}$ ,  $i_{la}$  (5 A/div),  $u_{cua}$ ,  $u_{cla}$  (1 V/div).

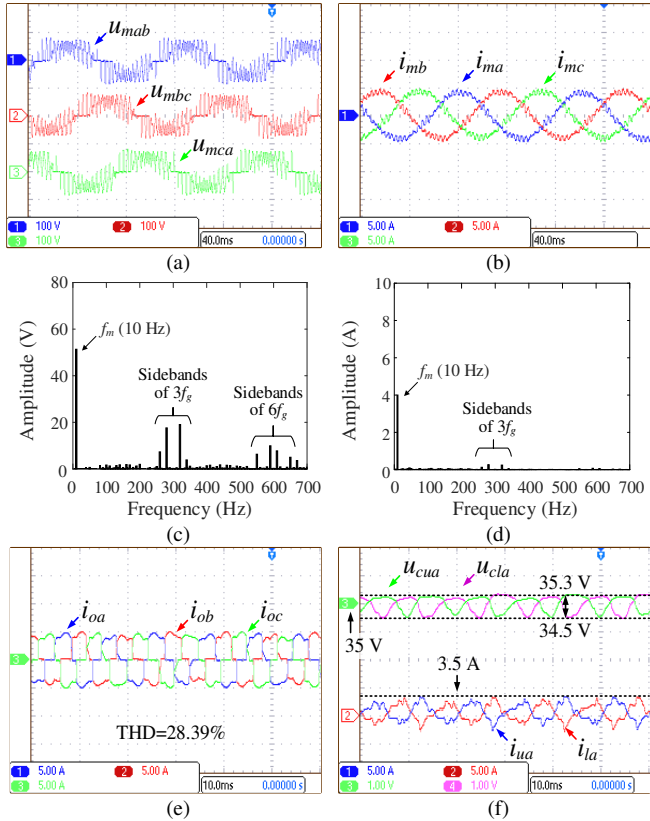


Fig. 20. Experimental waveforms under 0.5 p.u. load. (a)  $u_{mab}$ ,  $u_{mbc}$ ,  $u_{mca}$  (100 V/div). (b)  $i_{ma}$ ,  $i_{mb}$ ,  $i_{mc}$  (5 A/div). (c) Spectrum of  $u_{mab}$ . (d) Spectrum of  $i_{ma}$ . (e)  $i_{oa}$ ,  $i_{ob}$ ,  $i_{oc}$  (5 A/div). (f)  $i_{ua}$ ,  $i_{la}$ ,  $u_{cua}$ ,  $u_{cia}$  (1 V/div).

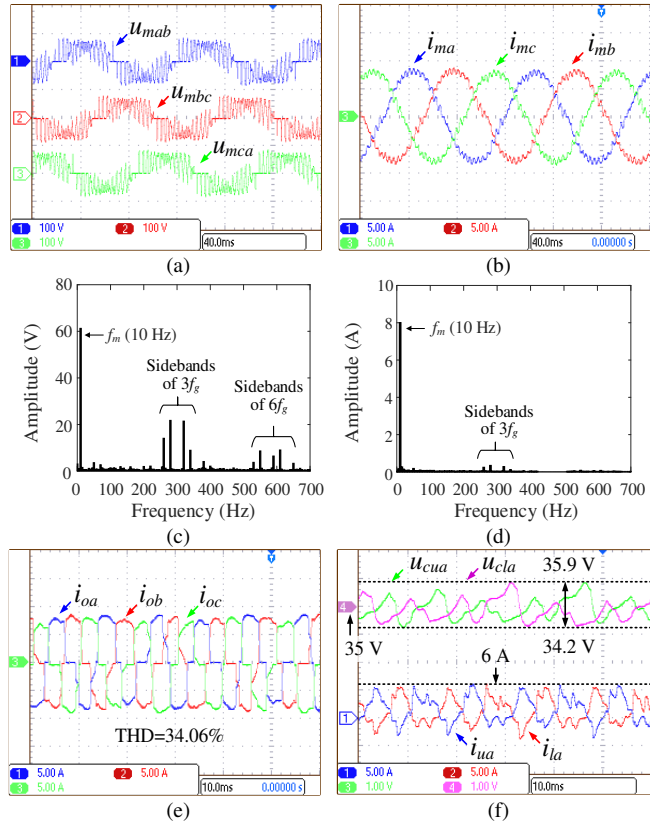


Fig. 21. Experimental waveforms at rated situation. (a)  $u_{mab}$ ,  $u_{mbc}$ ,  $u_{mca}$  (100 V/div). (b)  $i_{ma}$ ,  $i_{mb}$ ,  $i_{mc}$  (5 A/div). (c) Spectrum of  $u_{mab}$ . (d) Spectrum of  $i_{ma}$ . (e)  $i_{oa}$ ,  $i_{ob}$ ,  $i_{oc}$  (5 A/div). (f)  $i_{ua}$ ,  $i_{la}$ ,  $u_{cua}$ ,  $u_{cia}$  (1 V/div).

reaches the maximum 6 A.

The SM capacitor voltage fluctuation also increases as the machine speed and torque increase. At rated situation, the voltage fluctuation reaches the upper limit, which ranges from 34.2 to 35.9 V. The voltage fluctuation ratio  $\varepsilon$  is 2.57% under the  $C_{sm}$  of 2.7 mF. According to (24)~(27) and experiment parameters in Table II, Fig. 22 shows the required  $C_{sm}$  under various  $\varepsilon$ . The estimated  $\varepsilon$  is 2.6% when  $C_{sm}$  is 2.7 mF, and accordingly the experimental result is almost consistent with the theoretical analysis.

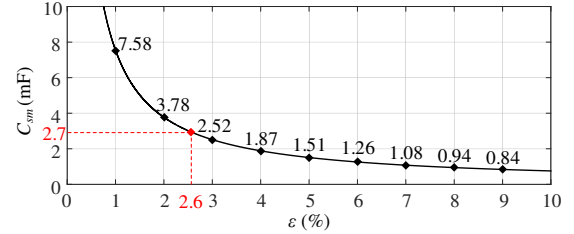


Fig. 22. Theoretical analysis of voltage fluctuation ratio under experimental parameters.

Fig. 23 shows the machine torque ripple at different operation situation. It can be observed that the torque ripple reaches the upper limit at rated situation, which is 0.12 p.u. as shown in Fig. 23(d).

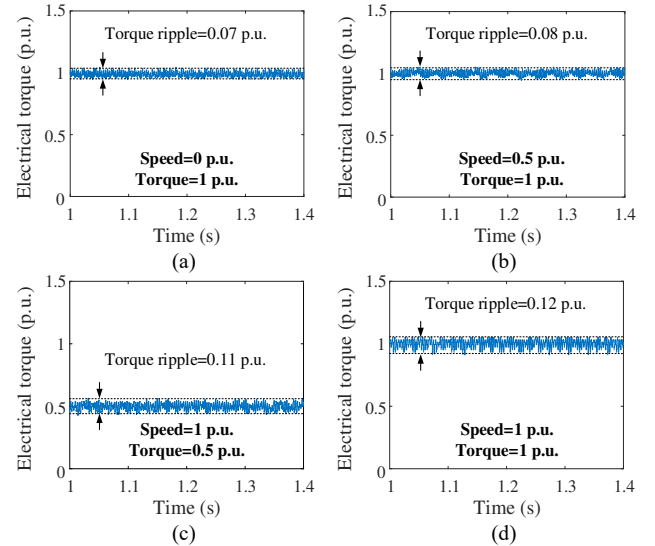


Fig. 23. Electrical torque in the experiment. (a) Electrical torque at standstill under rated load. (b) Electrical torque at 0.5 p.u. speed under rated load. (c) Electrical torque at rated speed under 0.5 p.u. load. (d) Electrical torque at rated situation.

## B. Dynamic Performance

Fig. 24 shows the dynamic performance when the machine operates from standstill to the rated frequency (10Hz) under rated load. Fig. 24(a) shows the machine line voltages  $u_{mab}$ ,  $u_{mbc}$ ,  $u_{mca}$ . Fig. 24(b) shows the machine currents  $i_{ma}$ ,  $i_{mb}$ ,  $i_{mc}$ , whose fundamental frequency amplitude is 8 A. Fig. 24(c) shows the MMC's output currents  $i_{oa}$ ,  $i_{ob}$ ,  $i_{oc}$ . Fig. 24(d) shows the arm currents and the SM capacitor voltages in phase  $a$  of the MMC. The peak of arm current increases with the machine speed, and its maximum value is 6 A. The voltage fluctuation of SM capacitors rises with the speed, and the maximum voltage fluctuation ratio is 2.57%.

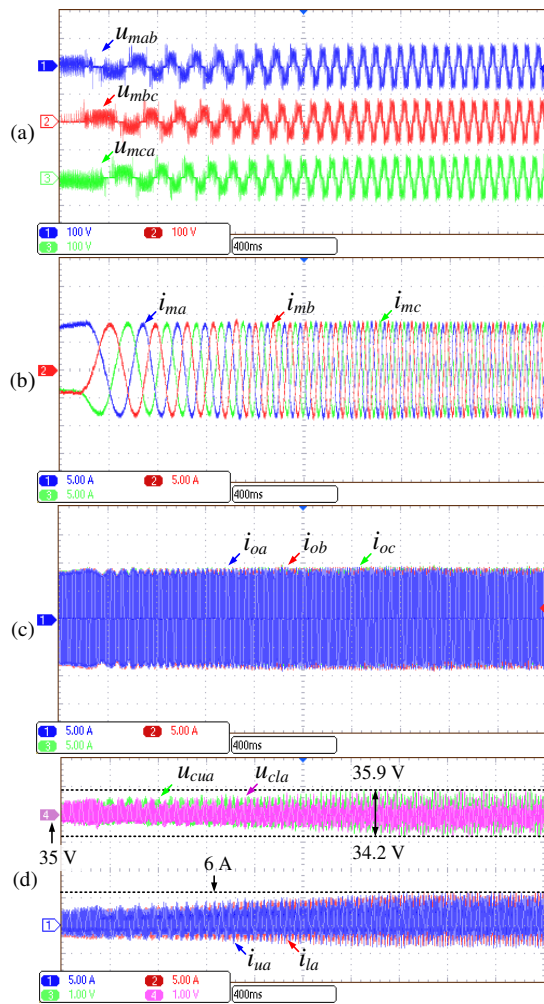


Fig. 24. Experimental waveforms when the system operates from standstill to rated speed. (a)  $u_{mab}$ ,  $u_{mbc}$ ,  $u_{mca}$  (100 V/div). (b)  $i_{ma}$ ,  $i_{mb}$ ,  $i_{mc}$  (5 A/div). (c)  $i_{0a}$ ,  $i_{0b}$ ,  $i_{0c}$  (5 A/div). (d)  $i_{ua}$ ,  $i_{la}$  (5 A/div),  $u_{cua}$ ,  $u_{cla}$  (1 V/div).

## VII. CONCLUSION

This paper proposes a cascaded MMC and CCV based machine drive system, which can operate stably at zero/low frequency. In the proposed system, the MMC operates at the medium frequency, providing constant ac voltage for the CCV. The CCV converts the medium-frequency ac input to low-frequency ac output required by the machine. The range of MMC's operation frequency is analyzed based on the safety commutation of thyristors in the CCV. Considering the fundamental and harmonic components of MMC's output current, the device current stress in the MMC is analyzed. The SM capacitance is also analyzed, which is significantly smaller than the existing MMC based methods. Simulation and experiment are conducted and their results verify the effectiveness of proposed machine drive system.

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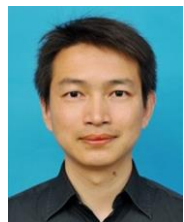


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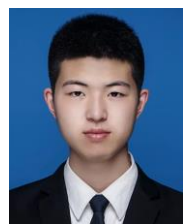
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